

### FEATURES

- High performance 24-bit  $\Sigma$ - $\Delta$  ADC
- 115 dB dynamic range at 78 kHz output data rate
- 109 dB dynamic range at 312 kHz output data rate
- 312 kHz maximum fully filtered output word rate
- Pin-selectable oversampling rate (64 $\times$ , 128 $\times$ , and 256 $\times$ )
- Low power mode
- Flexible SPI
- Fully differential modulator input
- On-chip differential amplifier for signal buffering
- On-chip reference buffer
- Full band low-pass finite impulse response (FIR) filter
- Overrange alert pin
- Digital gain correction registers
- Power-down mode
- Synchronization of multiple devices via  $\overline{\text{SYNC}}$  pin
- Daisy chaining

### APPLICATIONS

- Data acquisition systems
- Vibration analysis
- Instrumentation

### GENERAL DESCRIPTION

The AD7764 is a high performance, 24-bit  $\Sigma$ - $\Delta$  analog-to-digital converter (ADC). It combines wide input bandwidth, high speed, and performance of 109 dB dynamic range at a 312 kHz output data rate. With excellent dc specifications, the converter is ideal for high speed data acquisition of ac signals where dc data is also required.

Using the AD7764 eases the front-end antialias filtering requirements, simplifying the design process significantly. The AD7764 offers pin-selectable decimation rates of 64 $\times$ , 128 $\times$ , and 256 $\times$ . Other features include an integrated buffer to drive the reference as well as a fully differential amplifier to buffer and level shift the input to the modulator.

An overrange alert pin indicates when an input signal has exceeded the acceptable range. The addition of internal gain and internal overrange registers make the AD7764 a compact, highly integrated data acquisition device requiring minimal peripheral components.

The AD7764 also offers a low power mode, significantly reducing power dissipation without reducing the output data rate or available input bandwidth.

### FUNCTIONAL BLOCK DIAGRAM

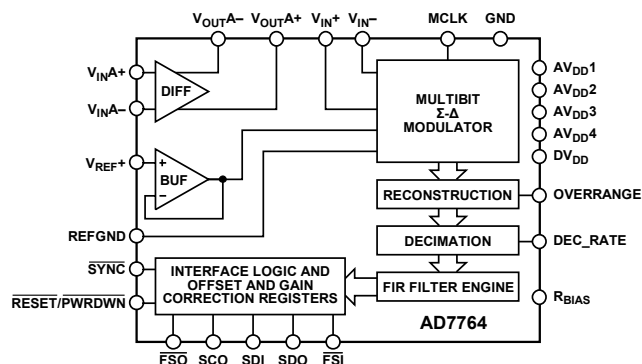


Figure 1.

The differential input is sampled at up to 40 MSPS by an analog modulator. The modulator output is processed by a series of low-pass filters. The external clock frequency applied to the AD7764 determines the sample rate, filter corner frequencies, and output word rate.

The AD7764 device boasts a full band on-board FIR filter. The full stop-band attenuation of the filter is achieved at the Nyquist frequency. This feature offers increased protection from signals that lie above the Nyquist frequency being aliased back into the input signal bandwidth.

The reference voltage supplied to the AD7764 determines the input range. With a 4 V reference, the analog input range is  $\pm 3.2768$  V differential biased around a common mode of 2.048 V. This common-mode biasing can be achieved using the on-chip differential amplifier, further reducing the external signal conditioning requirements.

The AD7764 is available in a 28-lead TSSOP package and is specified over the industrial temperature range from  $-40^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ .

Table 1. Related Devices

Part No.	Description
<a href="#">AD7760</a>	2.5 MSPS, 100 dB, parallel output on-chip buffers
<a href="#">AD7762</a>	625 kSPS, 109 dB, parallel output on-chip buffers
<a href="#">AD7763</a>	625 kSPS, 109 dB, serial output, on-chip buffers
<a href="#">AD7765</a>	156 kSPS, 112 dB, serial output, on-chip buffers
<a href="#">AD7766</a>	125 kSPS, 108 dB, serial output, 20 mW max power
<a href="#">AD7767</a>	125 kSPS, 108 dB, serial output, 20 mW max Power

### Rev. 0

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## REVISION HISTORY

6/07—Revision 0: Initial Version

## SPECIFICATIONS

$AV_{DD1} = DV_{DD} = V_{DRIVE} = 2.5\text{ V}$ ,  $AV_{DD2} = AV_{DD3} = AV_{DD4} = 5\text{ V}$ ,  $V_{REF+} = 4.096\text{ V}$ , MCLK amplitude = 5 V,  $T_A = 25^\circ\text{C}$ , normal power mode, using the on-chip amplifier with components, as shown in Table 11, unless otherwise noted.<sup>1</sup>

**Table 2.**

Parameter	Test Conditions/Comments	Specification	Unit
<b>DYNAMIC PERFORMANCE</b>			
Decimate 256×			
Normal Power Mode	MCLK = 40 MHz, ODR = 78.125 kHz, $f_{IN} = 1\text{ kHz}$ sine wave		
Dynamic Range	Modulator inputs shorted	115	dB typ
		110	dB min
	Differential amplifier inputs shorted	113.4	dB typ
Signal-to-Noise Ratio (SNR) <sup>2</sup>	Input amplitude = -0.5 dB	109	dB typ
		106	dB min
Spurious-Free Dynamic Range (SFDR)	Nonharmonic	130	dBFS typ
Total Harmonic Distortion (THD)	Input amplitude = -0.5 dB	-105	dB typ
	Input amplitude = -6 dB	-103	dB typ
	Input amplitude = -60 dB	-71	dB typ
Low Power Mode	MCLK = 40 MHz, ODR = 78.125 kHz, $f_{IN} = 1\text{ kHz}$ sine wave		
Dynamic Range	Modulator inputs shorted	113	dB typ
		110	dB min
	Differential amplifier inputs shorted	112	dB typ
Signal-to-Noise Ratio (SNR) <sup>2</sup>	Input amplitude = -0.5 dB	109	dB typ
		106	dB min
Total Harmonic Distortion (THD)	Input amplitude = -0.5 dB	-105	dB typ
	Input amplitude = -6 dB	-111	dB typ
	Input amplitude = -6 dB	-100	dB max
	Input amplitude = -60 dB	-76	dB typ
Decimate 128×			
Normal Power Mode	MCLK = 40 MHz, ODR = 156.25 kHz, $f_{IN} = 1\text{ kHz}$ sine wave		
Dynamic Range	Modulator inputs shorted	112	dB typ
		108	dB min
	Differential amplifier inputs shorted	110.4	dB typ
Signal-to-Noise Ratio (SNR) <sup>2</sup>		107	dB typ
		105	dB min
Spurious-Free Dynamic Range (SFDR)	Nonharmonic	130	dBFS typ
Total Harmonic Distortion (THD)	Input amplitude = -0.5 dB	-105	dB typ
	Input amplitude = -6 dB	-103	dB typ
Intermodulation Distortion (IMD)	Input amplitude = -6 dB, $f_{IN\text{ A}} = 50.3\text{ kHz}$ , $f_{IN\text{ B}} = 47.3\text{ kHz}$		
	Second-order terms	-117	dB typ
	Third-order terms	-108	dB typ
Low Power Mode	MCLK = 40 MHz, ODR = 156.25 kHz, $f_{IN} = 1\text{ kHz}$ sine wave		
Dynamic Range	Modulator inputs shorted	110	dB typ
		109	dB min
	Differential amplifier inputs shorted	109	dB typ
Signal-to-Noise Ratio (SNR) <sup>2</sup>	Input amplitude = -0.5 dB	107	dB typ
		105	dB min
Total Harmonic Distortion (THD)	Input amplitude = -0.5 dB	-105	dB typ
	Input amplitude = -6 dB	-111	dB typ
	Input amplitude = -6 dB	-100	dB max
Intermodulation Distortion (IMD)	Input amplitude = -6 dB, $f_{IN\text{ A}} = 50.3\text{ kHz}$ , $f_{IN\text{ B}} = 47.3\text{ kHz}$		
	Second-order terms	-134	dB typ
	Third-order terms	-110	dB typ

# AD7764

Parameter	Test Conditions/Comments	Specification	Unit
Decimate 64x			
Normal Power Mode	MCLK = 40 MHz, ODR = 312.5 kHz, $f_{IN}$ = 1 kHz sine wave		
Dynamic Range	Modulator inputs shorted	109	dB typ
		105	dB min
	Differential amplifier inputs shorted	107.3	dB typ
Signal-to-Noise Ratio (SNR) <sup>2</sup>		104	dB typ
		102.7	dB min
Spurious-Free Dynamic Range (SFDR)	Nonharmonic	130	dBFS typ
Total Harmonic Distortion (THD)	Input amplitude = –0.5 dB	–105	dB typ
	Input amplitude = –6 dB	–103	dB typ
Intermodulation Distortion (IMD)	Input amplitude = –6 dB, $f_{IN A}$ = 100.3 kHz, $f_{IN B}$ = 97.3 kHz		
	Second-order terms	–118	dB
	Third-order terms	–108	dB
Low Power Mode			
Dynamic Range	Modulator inputs shorted	106	dB typ
		105	dB min
	Differential amplifier inputs shorted	105.3	
Signal-to-Noise Ratio (SNR) <sup>2</sup>	Input amplitude = –0.5 dB	103	dB typ
		102	dB min
Spurious-Free Dynamic Range (SFDR)	Nonharmonic	110	dBFS typ
Total Harmonic Distortion (THD)	Input amplitude = –0.5 dB	–105	dB typ
	Input amplitude = –6 dB	–111	dB typ
		–100	dB max
DC ACCURACY			
Resolution	Guaranteed monotonic to 24 bits	24	Bits
Integral Nonlinearity	Normal power mode	0.0036	% typ
	Low power mode	0.0014	% typ
Zero Error	Normal power mode	0.006	% typ
		0.03	% max
	Including on-chip amplifier	0.04	% typ
	Low power mode	0.002	% typ
		0.024	% max
Gain Error		0.018	% typ
	Including on-chip amplifier	0.04	% typ
Zero Error Drift		0.00006	%FS/°C typ
Gain Error Drift		0.00005	%FS/°C typ
DIGITAL FILTER CHARACTERISTICS			
Pass-Band Ripple		0.1	dB typ
Pass Band <sup>3</sup>	–1 dB frequency	ODR × 0.4016	kHz
–3 dB Bandwidth <sup>3</sup>		ODR × 0.4096	kHz
Stop Band <sup>3</sup>	Beginning of stop band	ODR × 0.5	kHz
Stop-Band Attenuation	Decimate 64x and decimate 128x modes	–120	dB typ
	Decimate 256x	–115	dB typ
Group Delay			
Decimate 64x	MCLK = 40 MHz	89	μs typ
Decimate 128x	MCLK = 40 MHz	177	μs typ
Decimate 256x	MCLK = 40 MHz	358	μs typ
ANALOG INPUT			
Differential Input Voltage	Modulator input pins: $V_{IN(+)} - V_{IN(-)}$ , $V_{REF+}$ = 4.096 V	±3.2768	V p-p
Input Capacitance	At on-chip differential amplifier inputs	5	pF typ
	At modulator inputs	29	pF typ

Parameter	Test Conditions/Comments	Specification	Unit
REFERENCE INPUT/OUTPUT			
V <sub>REF</sub> Input Voltage	AV <sub>DD3</sub> = 5 V ± 5%	4.096	V
V <sub>REF</sub> Input DC Leakage Current		±1	μA max
V <sub>REF</sub> Input Capacitance		5	pF typ
DIGITAL INPUT/OUTPUT			
MCLK Input Amplitude		2.25 to 5.25	V
Input Capacitance		7.3	pF typ
Input Leakage Current		±1	μA/pin max
V <sub>INH</sub>		0.8 × DV <sub>DD</sub>	V min
V <sub>INL</sub>		0.2 × DV <sub>DD</sub>	V max
V <sub>OH</sub> <sup>4</sup>		2.2	V min
V <sub>OL</sub>		0.1	V max
ON-CHIP DIFFERENTIAL AMPLIFIER			
Input Impedance		>1	MΩ
Bandwidth for 0.1 dB Flatness		125	kHz
Common-Mode Input Voltage	Voltage range at input pins: V <sub>IN</sub> A+ and V <sub>IN</sub> A–	–0.5 to +2.2	V
Common-Mode Output Voltage	On-chip differential amplifier pins: V <sub>OUT</sub> + and V <sub>OUT</sub> –	2.048	V
POWER REQUIREMENTS			
AV <sub>DD1</sub> (Modulator Supply)	±5%	2.5	V
AV <sub>DD2</sub> (General Supply)	±5%	5	V
AV <sub>DD3</sub> (Differential Amplifier Supply)	±5%	5	V min/max
AV <sub>DD4</sub> (Ref Buffer Supply)	±5%	5	V min/max
DV <sub>DD</sub>	±5%	2.5	V
Normal Power Mode			
Al <sub>DD1</sub> (Modulator)		19	mA typ
Al <sub>DD2</sub> (General) <sup>5</sup>	MCLK = 40 MHz	13	mA typ
Al <sub>DD3</sub> (Differential Amplifier)	AV <sub>DD3</sub> = 5 V	10	mA typ
Al <sub>DD4</sub> (Reference Buffer)	AV <sub>DD4</sub> = 5 V	9	mA typ
DI <sub>DD</sub> <sup>5</sup>	MCLK = 40 MHz	37	mA typ
Low Power Mode			
Al <sub>DD1</sub> (Modulator)		10	mA typ
Al <sub>DD2</sub> (General) <sup>5</sup>	MCLK = 40 MHz	7	mA typ
Al <sub>DD3</sub> (Differential Amplifier)	AV <sub>DD3</sub> = 5 V	5.5	mA typ
Al <sub>DD4</sub> (Reference Buffer)	AV <sub>DD4</sub> = 5 V	5	mA typ
DI <sub>DD</sub> <sup>5</sup>	MCLK = 40 MHz	20	mA typ
POWER DISSIPATION			
Normal Power Mode	MCLK = 40 MHz, decimate 64×	300	mW typ
		371	mW max
Low Power Mode	MCLK = 40 MHz, decimate 64×	160	mW typ
		215	mW max
Power-Down Mode <sup>6</sup>	PWRDWN held logic low	1	mW typ

<sup>1</sup> See Terminology section.<sup>2</sup> SNR specifications in decibels are referred to a full-scale input, FS. Tested with an input signal at 0.5 dB below full scale, unless otherwise specified.<sup>3</sup> Output Data Rate (ODR) = [(MCLK/2)]/Decimation Rate. That is, the maximum ODR for AD7764 = [(40 MHz)/2]/64 = 312.5 kHz.<sup>4</sup> Tested with a 400 μA load current.<sup>5</sup> Tested at MCLK = 40 MHz. This current scales linearly with MCLK frequency applied.<sup>6</sup> Tested at 125°C.

## TIMING SPECIFICATIONS

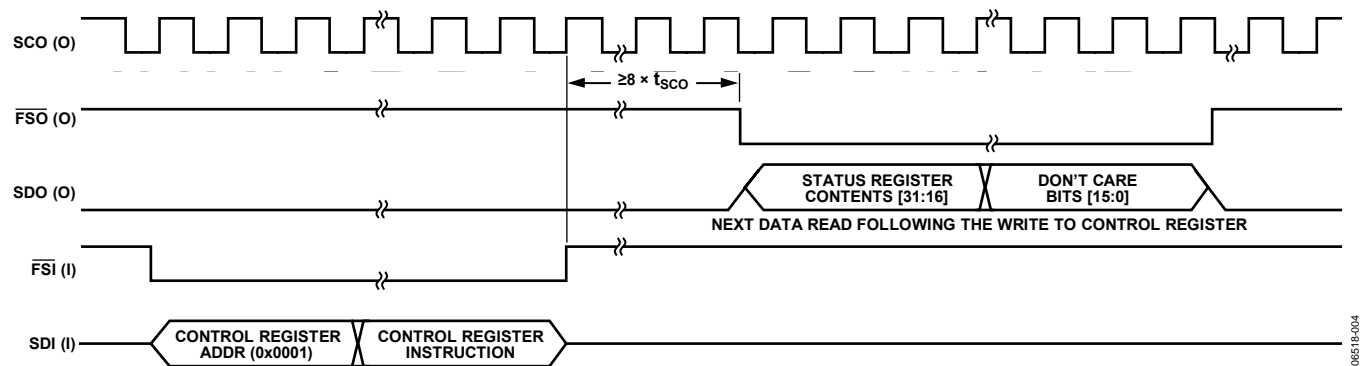
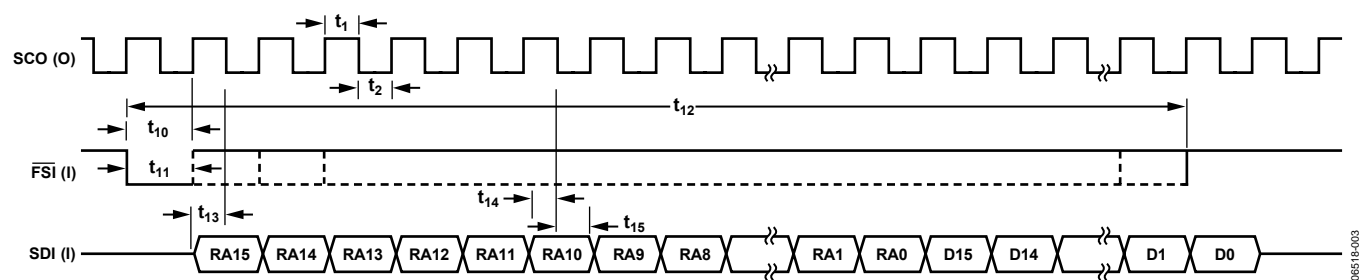
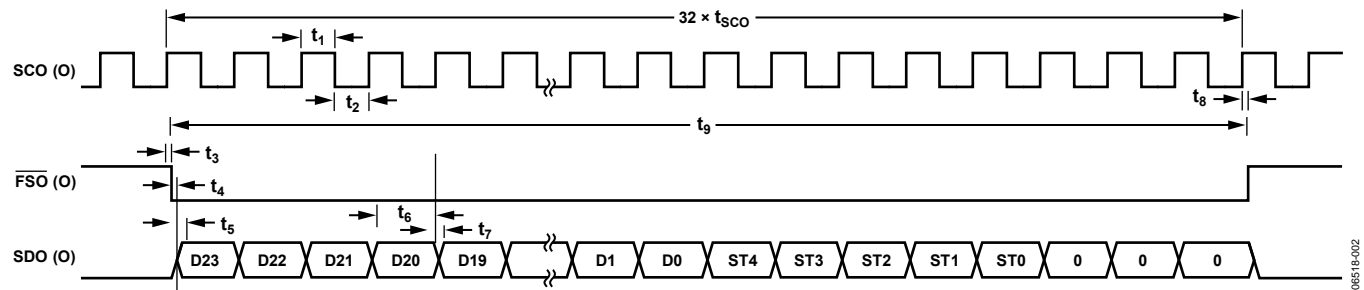
$AV_{DD1} = DV_{DD} = 2.5\text{ V}$ ,  $AV_{DD2} = AV_{DD3} = AV_{DD4} = 5\text{ V}$ ,  $V_{REF+} = 4.096\text{ V}$ ,  $T_A = 25^\circ\text{C}$ ,  $C_{LOAD} = 25\text{ pF}$ .

Table 3.

Parameter	Limit at $T_{MIN}$ , $T_{MAX}$	Unit	Description
$f_{MCLK}$	500 40	kHz min MHz max	Applied master clock frequency
$f_{ICLK}$	250 20	kHz min MHz max	Internal modulator clock derived from MCLK
$t_1$	$1 \times t_{ICLK}$	typ	SCO high period
$t_2$	$1 \times t_{ICLK}$	typ	SCO low period
$t_3$	1	ns typ	SCO rising edge to $\overline{FSO}$ falling edge
$t_4$	2	ns typ	Data access time, $\overline{FSO}$ falling edge to data active
$t_5$	8	ns max	MSB data access time, SDO active to SDO valid
$t_6$	40	ns min	Data hold time (SDO valid to SCO rising edge)
$t_7$	9.5	ns max	Data access time (SCO rising edge to SDO valid)
$t_8$	2	ns typ	SCO rising edge to $\overline{FSO}$ rising edge
$t_9$	$32 \times t_{SCO}$	max	$\overline{FSO}$ low period
$t_{10}$	12	ns min	Setup time from $\overline{FSI}$ falling edge to SCO falling edge
$t_{11}$	$1 \times t_{SCO}$	min	$\overline{FSI}$ low period
$t_{12}^1$	$32 \times t_{SCO}$	max	$\overline{FSI}$ low period
$t_{13}$	12	ns min	SDI setup time for the first data bit
$t_{14}$	12	ns min	SDI setup time
$t_{15}$	0	ns max	SDI hold time

<sup>1</sup> This is the maximum time  $\overline{FSI}$  can be held low when writing to an individual device (a device that is not daisy-chained).

TIMING DIAGRAMS



## ABSOLUTE MAXIMUM RATINGS

$T_A = 25^\circ\text{C}$ , unless otherwise noted.

**Table 4.**

Parameter	Rating
$AV_{DD1}$ to GND	$-0.3\text{ V to }+2.8\text{ V}$
$AV_{DD2}$ , $AV_{DD3}$ , $AV_{DD4}$ to GND	$-0.3\text{ V to }+6\text{ V}$
$DV_{DD}$ to GND	$-0.3\text{ V to }+2.8\text{ V}$
$V_{INA+}$ , $V_{INA-}$ to GND <sup>1</sup>	$-0.3\text{ V to }+6\text{ V}$
$V_{IN+}$ , $V_{IN-}$ to GND <sup>1</sup>	$-0.3\text{ V to }+6\text{ V}$
Digital Input Voltage to GND <sup>2</sup>	$-0.3\text{ V to }+2.8\text{ V}$
$V_{REF+}$ to GND <sup>3</sup>	$-0.3\text{ V to }+6\text{ V}$
AGND to DGND	$-0.3\text{ V to }+0.3\text{ V}$
Input Current to Any Pin Except Supplies <sup>4</sup>	$\pm 10\text{ mA}$
Operating Temperature Range	
Commercial	$-40^\circ\text{C to }+85^\circ\text{C}$
Storage Temperature Range	$-65^\circ\text{C to }+150^\circ\text{C}$
Junction Temperature	$150^\circ\text{C}$
TSSOP Package	
$\theta_{JA}$ Thermal Impedance	$143^\circ\text{C/W}$
$\theta_{JC}$ Thermal Impedance	$45^\circ\text{C/W}$
Lead Temperature, Soldering	
Vapor Phase (60 sec)	$215^\circ\text{C}$
Infrared (15 sec)	$220^\circ\text{C}$
ESD	$1\text{ kV}$

<sup>1</sup> Absolute maximum voltage for  $V_{IN-}$ ,  $V_{IN+}$ ,  $V_{INA-}$ , and  $V_{INA+}$  is  $6.0\text{ V}$  or  $AV_{DD3} + 0.3\text{ V}$ , whichever is lower.

<sup>2</sup> Absolute maximum voltage on digital inputs is  $3.0\text{ V}$  or  $DV_{DD} + 0.3\text{ V}$ , whichever is lower.

<sup>3</sup> Absolute maximum voltage on  $V_{REF+}$  input is  $6.0\text{ V}$  or  $AV_{DD4} + 0.3\text{ V}$ , whichever is lower.

<sup>4</sup> Transient currents of up to  $100\text{ mA}$  do not cause SCR latch-up.

Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. This is a stress rating only; functional operation of the device at these or any other conditions above those listed in the operational sections of this specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

### ESD CAUTION



#### ESD (electrostatic discharge) sensitive device.

Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.



## PIN CONFIGURATION AND FUNCTION DESCRIPTIONS

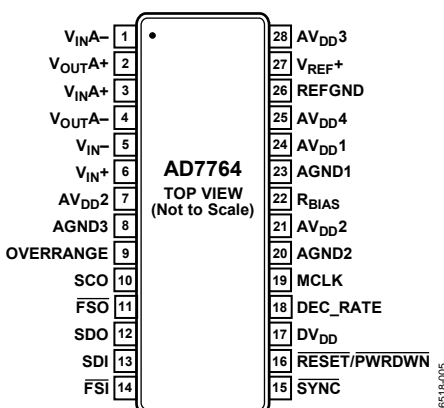


Figure 5. 28-Lead TSSOP Pin Configuration

Table 5. Pin Function Descriptions

Pin No.	Mnemonic	Description
24	AV <sub>DD</sub> 1	2.5 V Power Supply for Modulator. This pin should be decoupled to AGND1 (Pin 23) with a 100 nF capacitor.
7 and 21	AV <sub>DD</sub> 2	5 V Power Supply. Pin 7 should be decoupled to AGND3 (Pin 8) with a 100 nF capacitor. Pin 21 should be decoupled to AGND1 (Pin 23) with a 100 nF capacitor.
28	AV <sub>DD</sub> 3	3.3 V to 5 V Power Supply for Differential Amplifier. This pin should be decoupled to the ground plane with a 100 nF capacitor.
25	AV <sub>DD</sub> 4	3.3 V to 5 V Power Supply for Reference Buffer. This pin should be decoupled to AGND1 (Pin 23) with a 100 nF capacitor.
17	DV <sub>DD</sub>	2.5 V Power Supply for Digital Circuitry and FIR Filter. This pin should be decoupled to the ground plane with a 100 nF capacitor.
22	R <sub>BIAS</sub>	Bias Current Setting Pin. A resistor must be inserted between this pin and AGND. For more details, see the Bias Resistor Selection section.
23	AGND1	Power Supply Ground for Analog Circuitry.
20	AGND2	Power Supply Ground for Analog Circuitry.
8	AGND3	Power Supply Ground for Analog Circuitry.
26	REFGND	Reference Ground. Ground connection for the reference voltage.
27	V <sub>REF</sub> <sup>+</sup>	Reference Input.
1	V <sub>IN</sub> A <sup>-</sup>	Negative Input to Differential Amplifier.
2	V <sub>OUT</sub> A <sup>+</sup>	Positive Output from Differential Amplifier.
3	V <sub>IN</sub> A <sup>+</sup>	Positive Input to Differential Amplifier.
4	V <sub>OUT</sub> A <sup>-</sup>	Negative Output from Differential Amplifier.
5	V <sub>IN</sub> <sup>-</sup>	Negative Input to the Modulator.
6	V <sub>IN</sub> <sup>+</sup>	Positive Input to the Modulator.
9	OVERRANGE	Overrange Pin. This pin outputs a logic high to indicate that the user has applied an analog input that is approaching the limit of the analog input to the modulator.
10	SCO	Serial Clock Out. This clock signal is derived from the internal ICLK signal. The frequency of this clock is equal to ICLK. See the Clocking the AD7764 section for further details.
11	FSO	Frame Sync Out. This signal frames the serial data output and is 32 SCO periods wide.
12	SDO	Serial Data Out. Data and status are output on this pin during each serial transfer. Each bit is clocked out on an SCO rising edge and is valid on the falling edge. See the AD7764 Interface section for further details.
13	SDI	Serial Data In. The first data bit (MSB) must be valid on the next SCO falling edge after the FSI event is latched. 32 bits are required for each write; the first 16-bit word contains the device and register address, and the second word contains the data. See the AD7764 Interface section for further details.

# AD7764

Pin No.	Mnemonic	Description
14	FSI	Frame Sync Input. The status of this pin is checked on the falling edge of SCO. If this pin is low, then the first data bit is latched in on the next SCO falling edge. See the AD7764 Interface section for further details.
15	$\overline{\text{SYNC}}$	Synchronization Input. A falling edge on this pin resets the internal filter. This can be used to synchronize multiple devices in a system. See the Synchronization section for further details.
16	$\overline{\text{RESET/}}$ $\overline{\text{PWRDWN}}$	Reset/Power-down Pin. When a logic low is sensed on this pin, the part is powered down and all internal circuitry is reset.
19	MCLK	Master Clock Input. A low jitter digital clock must be applied to this pin. The output data rate depends on the frequency of this clock. See the Clocking the AD7764 section for more details.
18	DEC_RATE	Decimation Rate. This pin selects one of the three decimation rate modes. When 2.5 V is applied to this pin, a decimation rate 64 $\times$ is selected. A decimation rate of 128 $\times$ is selected by leaving the pin floating. A decimation rate of 256 $\times$ is selected by setting the pin to ground.

## TYPICAL PERFORMANCE CHARACTERISTICS

$AV_{DD1} = DV_{DD} = V_{DRIVE} = 2.5$  V,  $AV_{DD2} = AV_{DD3} = AV_{DD4} = 5$  V,  $V_{REF+} = 4.096$  V, MCLK amplitude = 5 V,  $T_A = 25^\circ\text{C}$ . Linearity plots are measured to 16-bit accuracy. The input signal is reduced to avoid modulator overload and digital clipping. Fast Fourier transforms (FFTs) of  $-0.5$  dB tones are generated from 262,144 samples in normal power mode. All other FFTs are generated from 8192 samples.

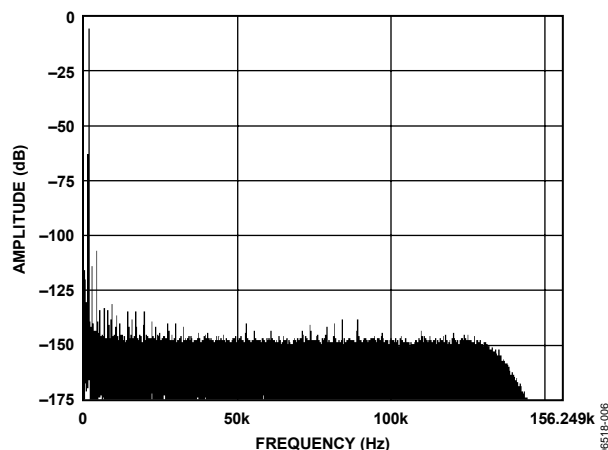


Figure 6. Normal Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 64x Decimation Rate

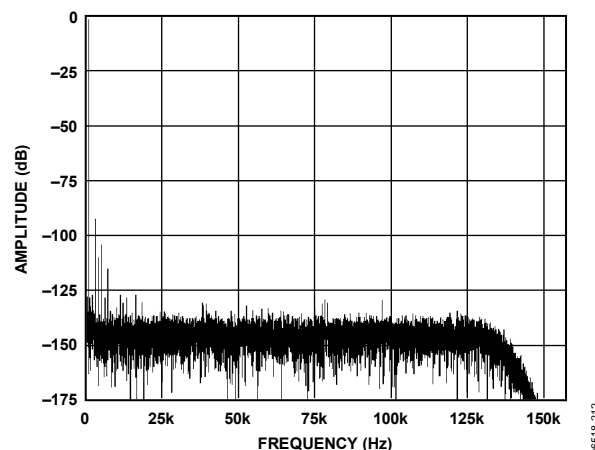


Figure 9. Low Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 64x Decimation Rate

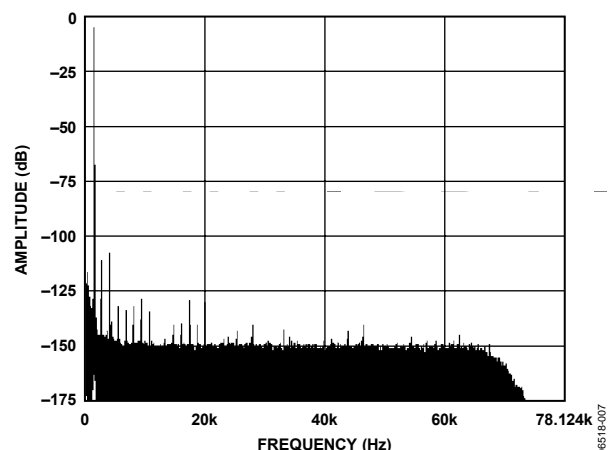


Figure 7. Normal Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 128x Decimation Rate

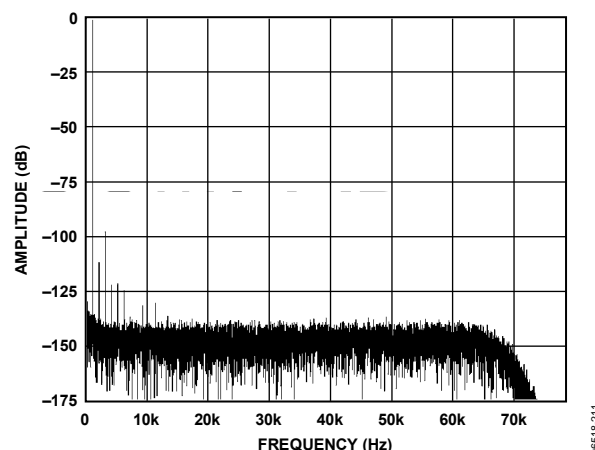


Figure 10. Low Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 128x Decimation Rate

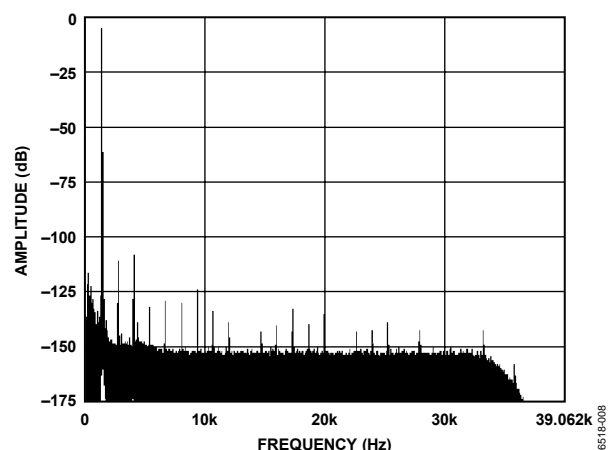


Figure 8. Normal Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 256x Decimation Rate

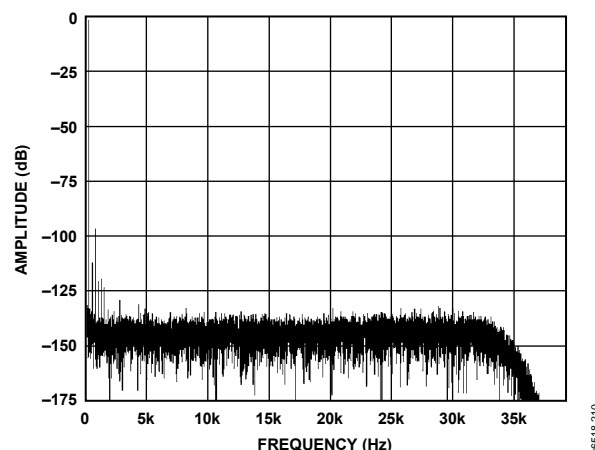


Figure 11. Low Power Mode, FFT, 1 kHz,  $-0.5$  dB Input Tone, 256x Decimation Rate

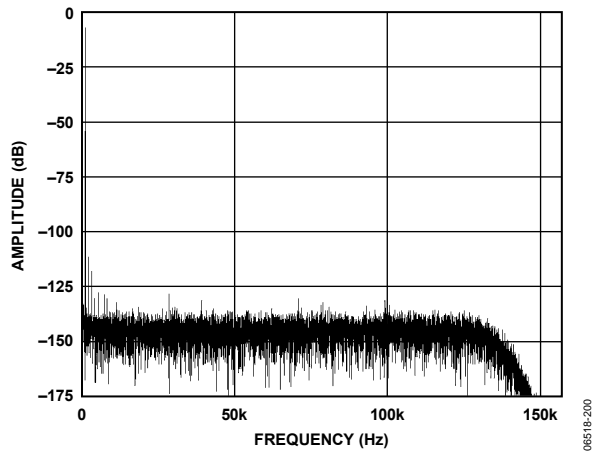


Figure 12. Normal Power Mode, FFT, 1 kHz, -6 dB Input Tone, 64x Decimation Rate

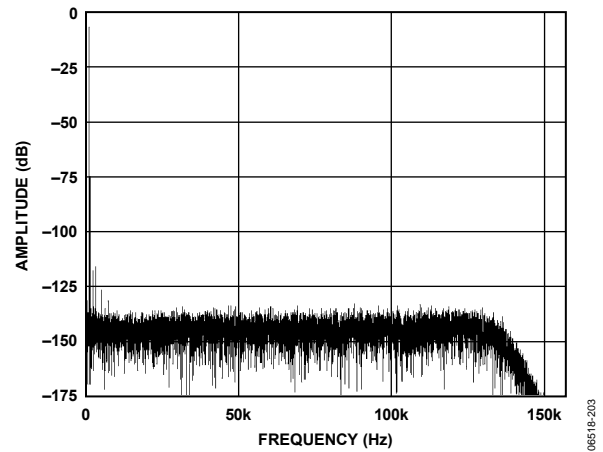


Figure 15. Low Power Mode, FFT, 1 kHz, -6 dB Input Tone, 64x Decimation Rate

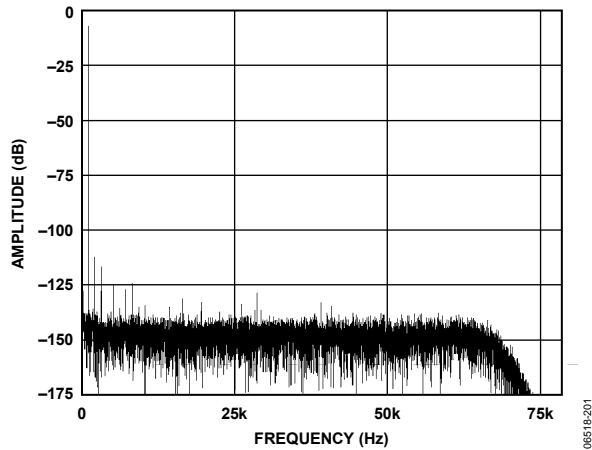


Figure 13. Normal Power Mode, FFT, 1 kHz, -6 dB Input Tone, 128x Decimation Rate

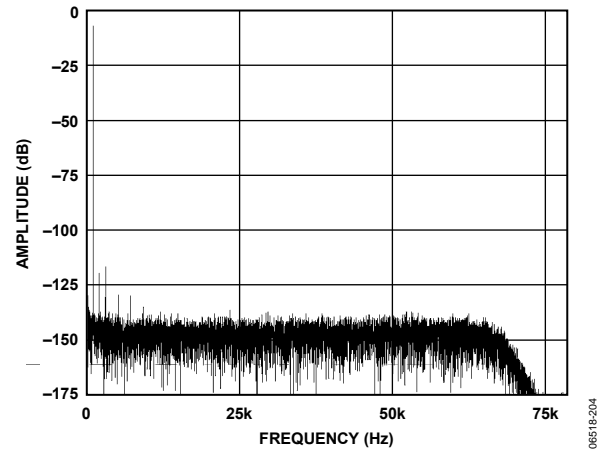


Figure 16. Low Power Mode, FFT, 1 kHz, -6 dB Input Tone, 128x Decimation Rate

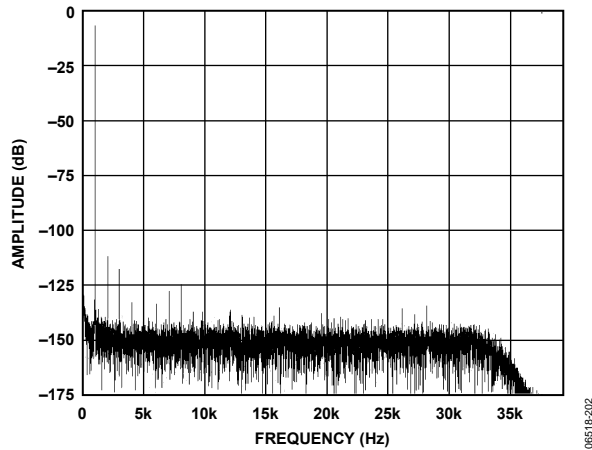


Figure 14. Normal Power Mode, FFT, 1 kHz, -6 dB Input Tone, 256x Decimation Rate

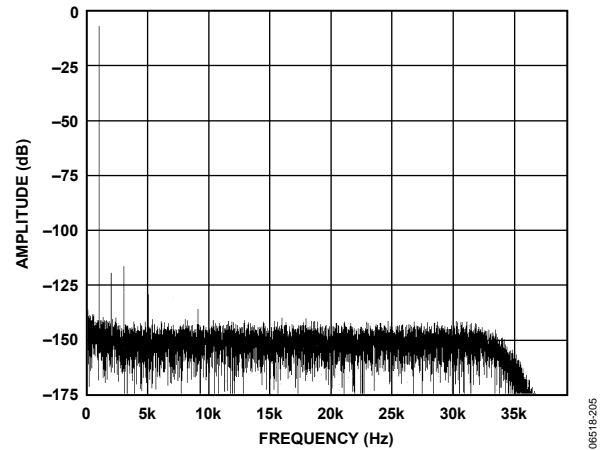


Figure 17. Low Power Mode, FFT, 1 kHz, -6 dB Input Tone, 256x Decimation Rate

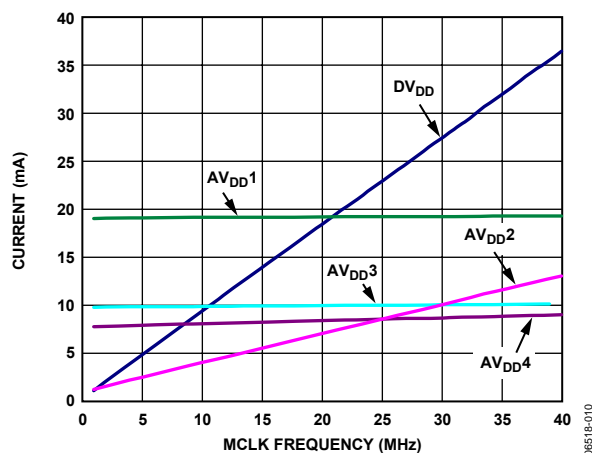


Figure 18. Normal Power Mode, Current Consumption vs. MCLK Frequency, 64x Decimation Rate

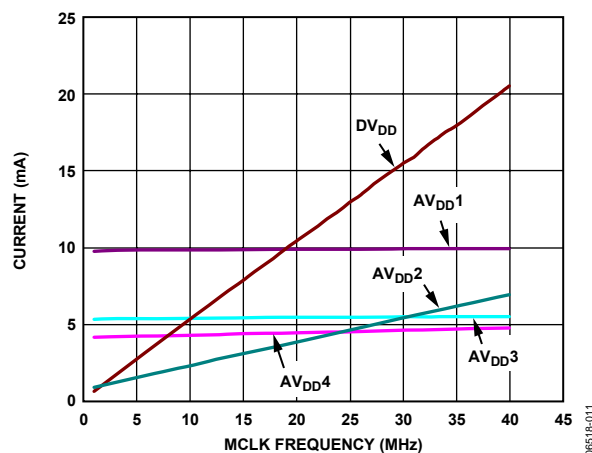


Figure 21. Low Power Mode, Current Consumption vs. MCLK Frequency, 64x Decimation Rate

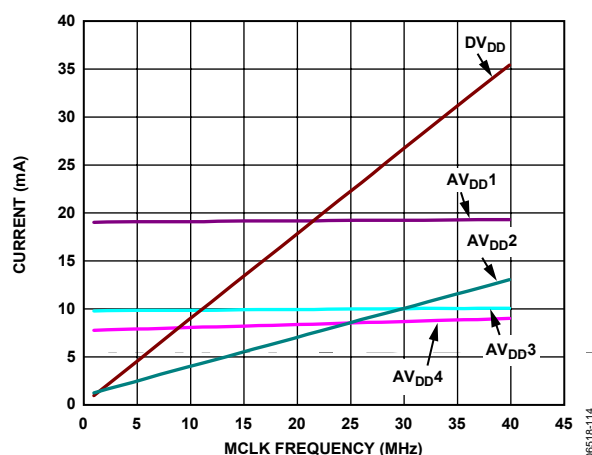


Figure 19. Normal Power Mode, Current Consumption vs. MCLK Frequency, 128x Decimation Rate

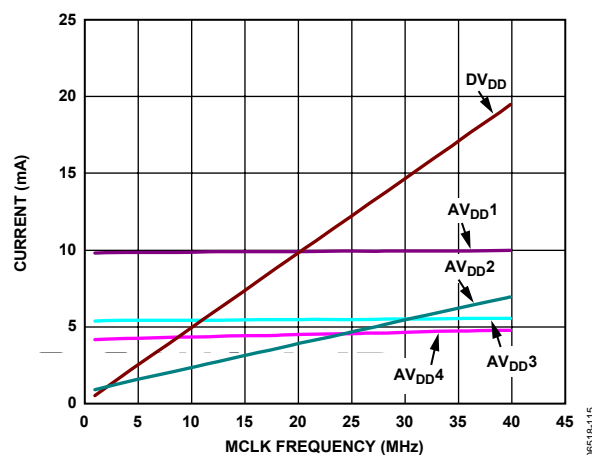


Figure 22. Low Power Mode, Current Consumption vs. MCLK Frequency, 128x Decimation Rate

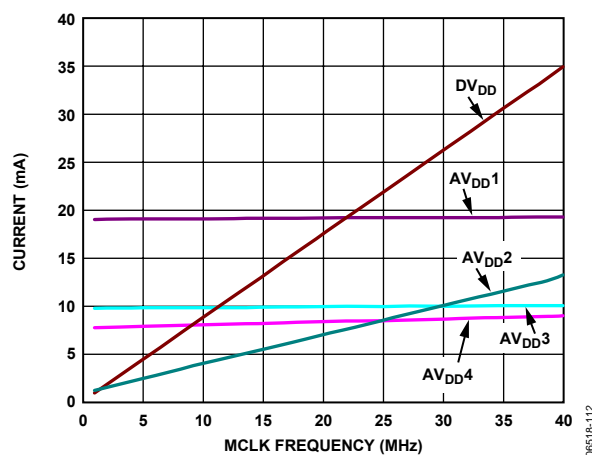


Figure 20. Normal Power Mode, Current Consumption vs. MCLK Frequency, 256x Decimation Rate

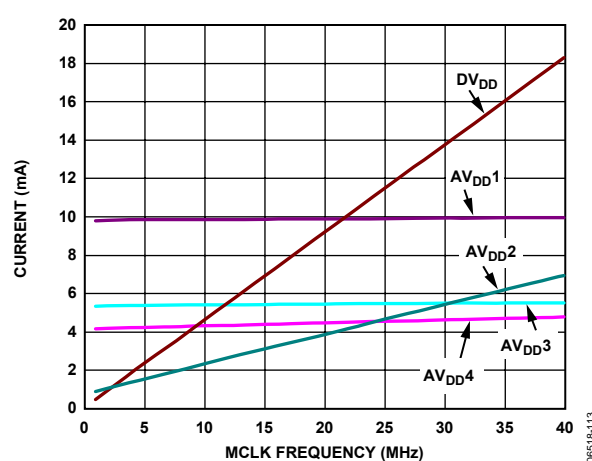


Figure 23. Low Power Mode, Current Consumption vs. MCLK Frequency, 256x Decimation Rate

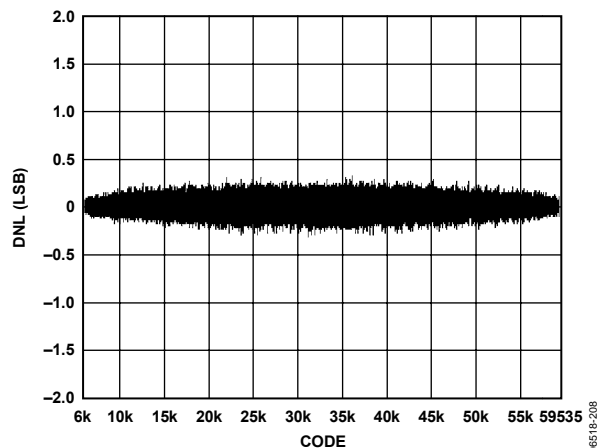


Figure 24. DNL Plot

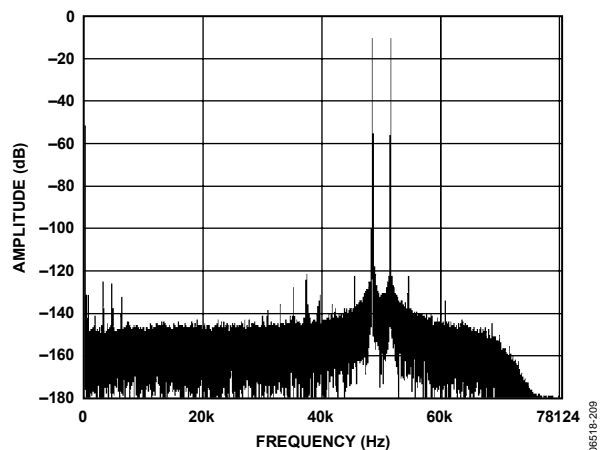


Figure 27. Normal Power Mode, IMD,  $f_{IN A} = 49.7$  kHz,  $f_{IN B} = 50.3$  kHz, 50 kHz Center Frequency, 128× Decimation Rate

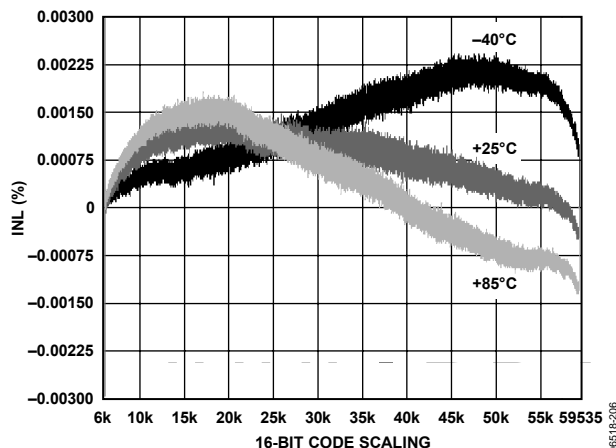


Figure 25. Normal Power Mode INL

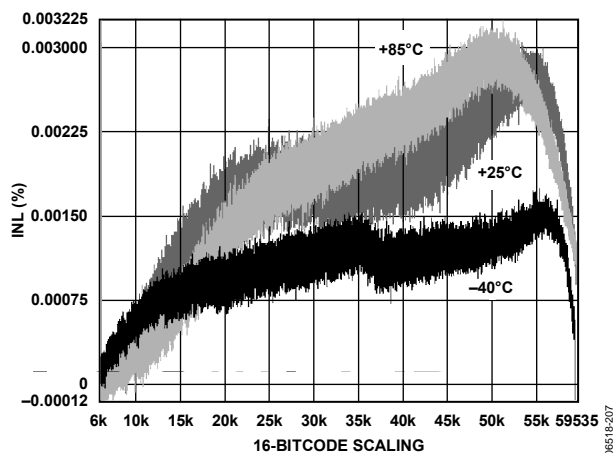


Figure 28. Low Power Mode INL

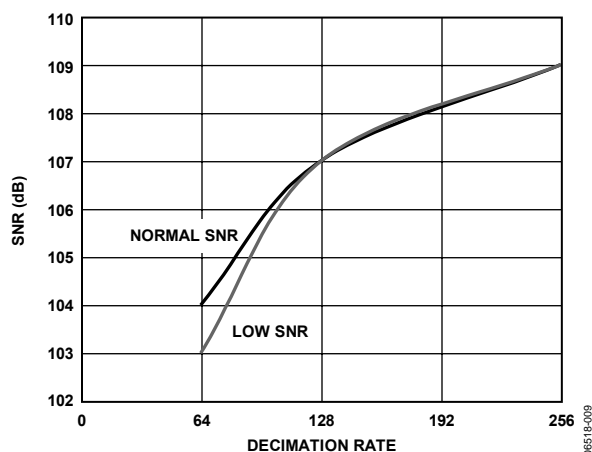


Figure 26. Normal and Low Power Mode, SNR vs. Decimation Rate, 1 kHz, -0.5 dB Input Tone

## TERMINOLOGY

### Signal-to-Noise Ratio (SNR)

The ratio of the rms value of the actual input signal to the rms sum of all other spectral components below the Nyquist frequency, excluding harmonics and dc. The value for SNR is expressed in decibels (dB).

### Total Harmonic Distortion (THD)

The ratio of the rms sum of harmonics to the fundamental. For the AD7764, it is defined as

$$THD(dB) = 20 \log \frac{\sqrt{V_2^2 + V_3^2 + V_4^2 + V_5^2 + V_6^2}}{V_1}$$

where:

$V_1$  is the rms amplitude of the fundamental.

$V_2$ ,  $V_3$ ,  $V_4$ ,  $V_5$ , and  $V_6$  are the rms amplitudes of the second to the sixth harmonics.

### Nonharmonic Spurious-Free Dynamic Range (SFDR)

The ratio of the rms signal amplitude to the rms value of the peak spurious spectral component, excluding harmonics.

### Dynamic Range

The ratio of the rms value of the full scale to the rms noise measured with the inputs shorted together. The value for dynamic range is expressed in decibels.

### Intermodulation Distortion

With inputs consisting of sine waves at two frequencies,  $f_a$  and  $f_b$ , any active device with nonlinearities creates distortion products at sum and difference frequencies of  $m f_a \pm n f_b$ , where  $m, n = 0, 1, 2, 3$ , and so on. Intermodulation distortion terms are those for which neither  $m$  nor  $n$  is equal to 0. For example, the second-order terms include  $(f_a + f_b)$  and  $(f_a - f_b)$ , while the third-order terms include  $(2f_a + f_b)$ ,  $(2f_a - f_b)$ ,  $(f_a + 2f_b)$ , and  $(f_a - 2f_b)$ .

The AD7764 is tested using the CCIF standard, where two input frequencies near the top end of the input bandwidth are used.

In this case, the second-order terms are usually distanced in frequency from the original sine waves, and the third-order terms are usually at a frequency close to the input frequencies. As a result, the second- and third-order terms are specified separately. The calculation of the intermodulation distortion is as per the THD specification, where it is the ratio of the rms sum of the individual distortion products to the rms amplitude of the sum of the fundamentals expressed in dB.

### Integral Nonlinearity (INL)

The maximum deviation from a straight line passing through the endpoints of the ADC transfer function.

### Differential Nonlinearity (DNL)

The difference between the measured and the ideal 1 LSB change between any two adjacent codes in the ADC.

### Zero Error

The difference between the ideal midscale input voltage (when

both inputs are shorted together) and the actual voltage producing the midscale output code.

### Zero Error Drift

The change in the actual zero error value due to a temperature change of 1°C. It is expressed as a percentage of full scale at room temperature.

### Gain Error

The first transition (from 100...000 to 100...001) should occur for an analog voltage 1/2 LSB above the nominal negative full scale. The last transition (from 011...110 to 011...111) should occur for an analog voltage 1 1/2 LSB below the nominal full scale. The gain error is the deviation of the difference between the actual level of the last transition and the actual level of the first transition, from the difference between the ideal levels.

### Gain Error Drift

The change in the actual gain error value due to a temperature change of 1°C. It is expressed as a percentage of full scale at room temperature.

## THEORY OF OPERATION

The AD7764 features an on-chip fully differential amplifier to feed the  $\Sigma$ - $\Delta$  modulator pins, an on-chip reference buffer, and a FIR filter block to perform the required digital filtering of the  $\Sigma$ - $\Delta$  modulator output. Using this  $\Sigma$ - $\Delta$  conversion technique with the added digital filtering, the analog input is converted to an equivalent digital word.

### $\Sigma$ - $\Delta$ MODULATION AND DIGITAL FILTERING

The input waveform applied to the modulator is sampled and an equivalent digital word is output to the digital filter at a rate equal to ICLK. By employing oversampling, the quantization noise is spread across a wide bandwidth from 0 to  $f_{\text{CLK}}/2$ . This means that the noise energy contained in the signal band of interest is reduced (see Figure 29). To further reduce the quantization noise, a high-order modulator is employed to shape the noise spectrum so that most of the noise energy is shifted out of the signal band (see Figure 30).

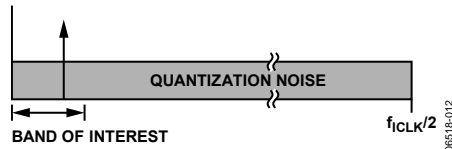


Figure 29.  $\Sigma$ - $\Delta$  ADC, Quantization Noise

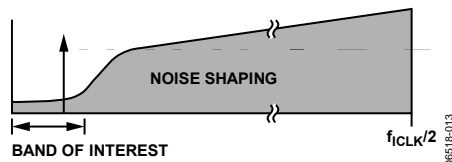


Figure 30.  $\Sigma$ - $\Delta$  ADC, Noise Shaping

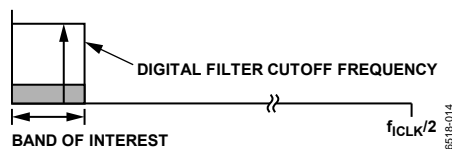


Figure 31.  $\Sigma$ - $\Delta$  ADC, Digital Filter Cutoff Frequency

The digital filtering that follows the modulator removes the large out-of-band quantization noise (see Figure 31) while also reducing the data rate from  $f_{\text{CLK}}$  at the input of the filter to  $f_{\text{CLK}}/64$  or less at the output of the filter, depending on the decimation rate used.

**Table 6. Configuration with Default Filter**

ICLK Frequency	Decimation Rate	Data State	Computation Delay	Filter Delay	SYNC to FILTER-SETTLE	Pass-Band Bandwidth	Output Data Rate (ODR)
20 MHz	64×	Fully filtered	2.25 $\mu$ s	87.6 $\mu$ s	$7122 \times t_{\text{MCLK}}$	125 kHz	312.5 kHz
20 MHz	128×	Fully filtered	3.1 $\mu$ s	174 $\mu$ s	$14217 \times t_{\text{MCLK}}$	62.5 kHz	156.25 kHz
20 MHz	256×	Fully filtered	4.65 $\mu$ s	346.8 $\mu$ s	$27895 \times t_{\text{MCLK}}$	31.25 kHz	78.125 kHz
12.288 MHz	64×	Fully filtered	3.66 $\mu$ s	142.6 $\mu$ s	$7122 \times t_{\text{MCLK}}$	76.8 kHz	192 kHz
12.288 MHz	128×	Fully filtered	5.05 $\mu$ s	283.2 $\mu$ s	$14217 \times t_{\text{MCLK}}$	38.4 kHz	96 kHz
12.288 MHz	256×	Fully filtered	7.57 $\mu$ s	564.5 $\mu$ s	$27895 \times t_{\text{MCLK}}$	19.2 kHz	48 kHz

The AD7764 employs three FIR filters in series. By using different combinations of decimation ratios, data can be obtained from the AD7764 at three data rates.

The first filter receives data from the modulator at ICLK MHz where it is decimated 4 $\times$  to output data at (ICLK/4) MHz. The second filter allows the decimation rate to be chosen from 8 $\times$  to 32 $\times$ .

The digital filtering on the AD7764 provides full-band filtering. This means that its stop-band attenuation occurs at the Nyquist frequency (ODR/2). This feature provides increased protection against aliasing of sampled frequencies that lie above the Nyquist rate (ODR/2). The filter gives maximum attenuation at the Nyquist rate (see Figure 32). This means that it attenuates all possible alias frequencies by 110 dB. The frequency response in Figure 32 occurs when the AD7764 is operated with a 40 MHz MCLK in the decimate 64 $\times$  mode. Note that the first stop-band frequency occurs at Nyquist. The frequency response of the filter scales with both the decimation rate chosen and the MCLK frequency applied.

The third filter has a fixed decimation rate of 2 $\times$ . Table 6 shows some characteristics of the digital filtering where ICLK = MCLK/2. The group delay of the filter is defined to be the delay to the center of the impulse response and is equal to the computation plus the filter delays. The delay until valid data is available (the FILTER-SETTLE status bit is set) is approximately twice the filter delay plus the computation delay. This is listed in terms of MCLK periods in Table 6.

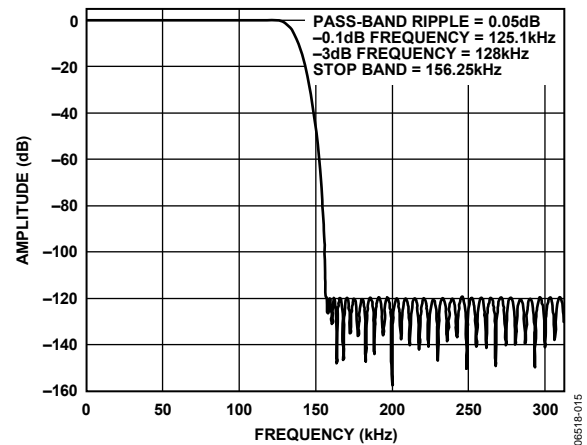


Figure 32. Filter Frequency Response (312.5 kHz ODR)



## AD7764 INPUT STRUCTURE

The AD7764 requires a 4.096 V input to the reference pin,  $V_{REF+}$ , supplied by a high precision reference, such as the ADR444. Because the input to the device's  $\Sigma$ - $\Delta$  modulator are fully differential, the effective differential reference range is 8.192 V.

$$V_{REF+(Diff)} = 2 \times 4.096 = 8.192 \text{ V}$$

As is inherent in  $\Sigma$ - $\Delta$  modulators, only a certain portion of this full reference may be used. With the AD7764, 80% of the full differential reference may be applied to the modulator's differential inputs.

$$Modulator\_Input_{FULLSCALE} = 8.192 \text{ V} \times 0.8 = 6.5536 \text{ V}$$

This means that a maximum of  $\pm 3.2768 \text{ V}$  p-p full-scale can be applied to each of the AD7764 modulator inputs (Pin 5 and Pin 6), with the AD7764 being specified with an input  $-0.5 \text{ dB}$  down from full scale ( $-0.5 \text{ dBFS}$ ).

The AD7764 modulator inputs must have a common-mode input of 2.048 V. Figure 33 shows the relative scaling between the differential voltages applied to the modulator pins, and the respective 24-bit two's complement digital outputs.

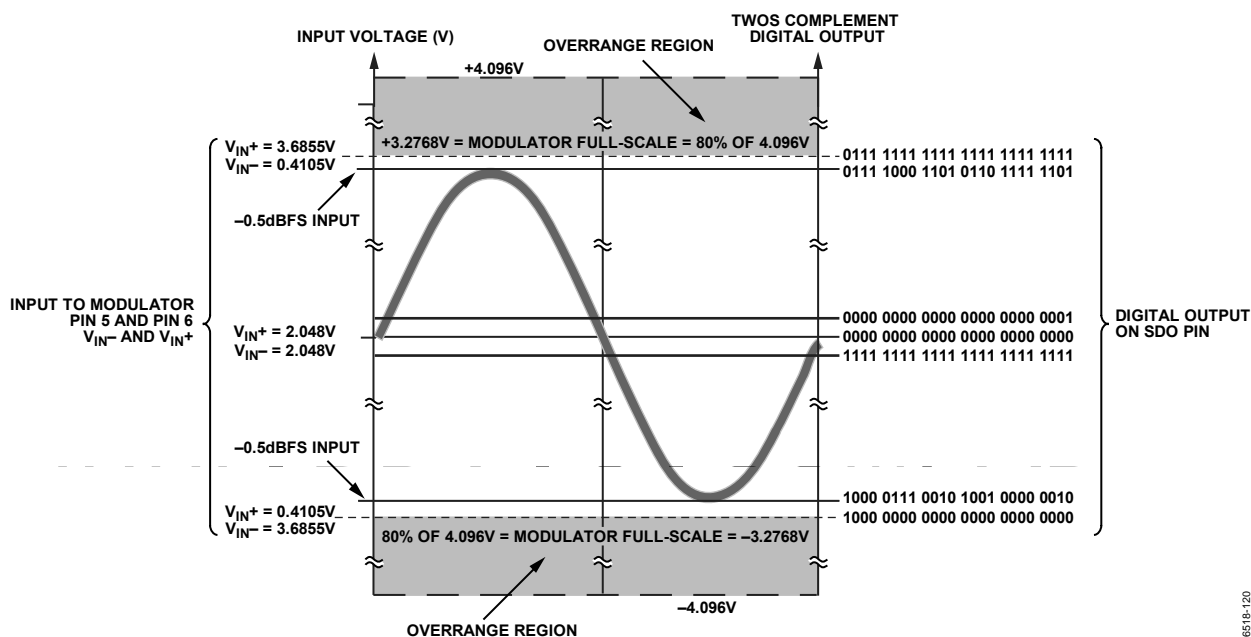


Figure 33. AD7764 Scaling: Modulator Input Voltage vs. Digital Output Code

08518-120

ON-CHIP DIFFERENTIAL AMPLIFIER

The AD7764 contains an on-board differential amplifier that is recommended to drive the modulator input pins. Pin 1, Pin 2, Pin 3, and Pin 4 on the AD7764 are the differential input and output pins of the amplifier. The external components,  $R_{IN}$ ,  $R_{FB}$ ,  $C_{FB}$ ,  $C_S$ , and  $R_M$ , are placed around Pin 1 through Pin 6 to create the recommended configuration.

To achieve the specified performance, the differential amplifier should be configured as a first-order antialias filter, as shown in Figure 34, using the component values listed in Table 7. The inputs to the differential amplifier are then routed through the external component network before being applied to the modulator inputs,  $V_{IN-}$  and  $V_{IN+}$ , (Pin 5 and Pin 6). Using the optimal values in the table as an example yields a 25 dB attenuation at the first alias point of 19.6 MHz.

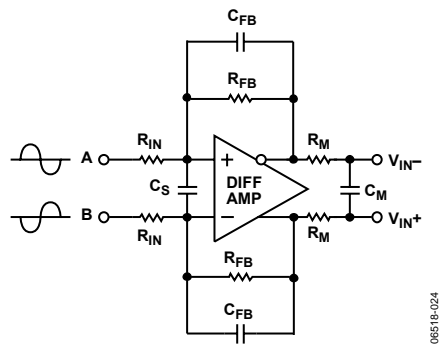


Figure 34. Differential Amplifier Configuration

Table 7. On-Chip Differential Filter Component Values

	$R_{IN}$ (k $\Omega$ )	$R_{FB}$ (k $\Omega$ )	$R_M$ ( $\Omega$ )	$C_S$ (pF)	$C_{FB}$ (pF)	$C_M$ (pF)
Optimal	4.75	3.01	43	8.2	47	33
Tolerance Range <sup>1</sup>	2.37 to 5.76	2.4 to 4.87	36 to 47	0 to 10	20 to 100	39 to 56

<sup>1</sup> Values shown are the acceptable tolerances for each component when altered relative to the optimal values used to achieve the stated specifications of the device.

The range of values for each of the components in the differential amplifier configuration is listed in Table 7. When using the differential amplifier to gain the input voltages to the required modulator input range, it is advisable to implement the gain function by changing  $R_{IN}$  and leaving the  $R_{FB}$  as the listed optimal value.

The common-mode input at each of the differential amplifier inputs (Pin  $V_{IN+}$  and Pin  $V_{IN-}$ ) can range from  $-0.5$  V dc to  $2.2$  V dc. The amplifier has a constant output common-mode voltage of  $2.048$  V, that is,  $V_{REF}/2$ , the requisite common mode voltage for the modulator input pins ( $V_{IN+}$  and  $V_{IN-}$ ).

Figure 35 shows the signal conditioning that occurs using the differential amplifier configuration detailed in Table 7 with a  $\pm 2.5$  V input signal to the differential amplifier. The amplifier in this example is biased around ground and is scaled to provide  $\pm 3.168$  V p-p ( $-0.5$  dBFS) on each modulator input with a  $2.048$  V common mode.

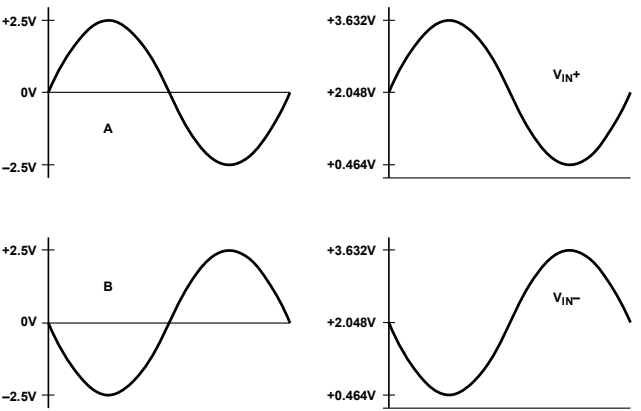


Figure 35. Differential Amplifier Signal Conditioning

To obtain maximum performance from the AD7764, it is advisable to drive the ADC with differential signals. Figure 36 shows how a bipolar, single-ended signal biased around ground can drive the AD7764 with the use of an external op amp, such as the AD8021.

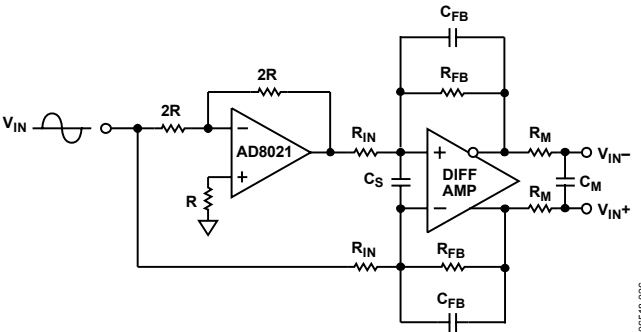


Figure 36. Single-Ended-to-Differential Conversion

MODULATOR INPUT STRUCTURE

The AD7764 employs a double-sampling front end, as shown in Figure 37. For simplicity, only the equivalent input circuitry for  $V_{IN+}$  is shown. The equivalent circuitry for  $V_{IN-}$  is the same.

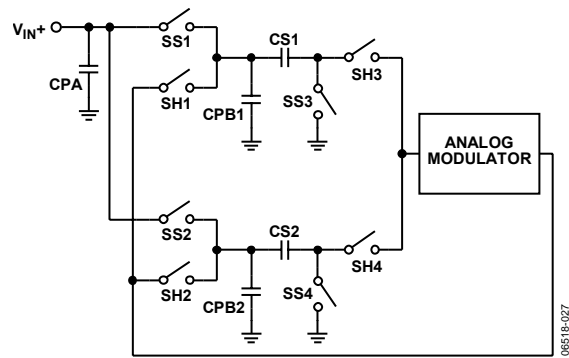


Figure 37. Equivalent Input Circuit

Sampling Switches SS1 and SS3 are driven by  $\overline{\text{ICLK}}$ , whereas Sampling Switches SS2 and SS4 are driven by  $\text{ICLK}$ . When  $\text{ICLK}$  is high, the analog input voltage is connected to CS1. On the falling edge of  $\text{ICLK}$ , the SS1 and SS3 switches open and the analog input is sampled on CS1. Similarly, when  $\text{ICLK}$  is low, the analog input voltage is connected to CS2. On the rising edge of  $\text{ICLK}$ , the SS2 and SS4 switches open, and the analog input is sampled on CS2.

Capacitors CPA, CPB1, and CPB2 represent parasitic capacitances that include the junction capacitances associated with the MOS switches.

Table 8. Equivalent Component Values

CS1	CS2	CPA	CPB1/2
13 pF	13 pF	13 pF	5 pF

## AD7764 INTERFACE

### READING DATA

The AD7764 uses an SPI-compatible serial interface. The timing diagram in Figure 2 shows how the AD7764 transmits its conversion results.

The data read from the AD7764 is clocked out using the serial clock output (SCO). The SCO frequency is half that of the MCLK input to the AD7764.

The conversion result output on the serial data output (SDO) line is framed by the frame synchronization output,  $\overline{\text{FSO}}$ , which is sent logic low for 32 SCO cycles. Each bit of the new conversion result is clocked onto the SDO line on the rising SCO edge and is valid on the falling SCO edge. The 32-bit result consists of the 24 data bits followed by five status bits followed further by three zeros. The five status bits are listed in Table 9 and described below the table.

**Table 9. Status Bits During Data Read**

D7	D6	D5	D4	D3
FILTER-SETTLE	OVR	LPWR	DEC_RATE 1	DEC_RATE 0

- The FILTER-SETTLE bit indicates whether the data output from the AD7764 is valid. After resetting the device (using the  $\overline{\text{RESET}}$  pin) or clearing the digital filter (using the  $\overline{\text{SYNC}}$  pin), the FILTER-SETTLE bit goes logic low to indicate that the full settling time of the filter has not yet passed and that the data is not yet valid. The FILTER-SETTLE bit also goes to zero when the input to the part has asserted the overrange alerts.
- The OVR (overrange) bit is described in the Overage Alerts section.
- The LPWR bit is set to logic high when the AD7764 is operating in low power mode. See the Power Modes section for further details.
- The DEC\_RATE 1 and DEC\_RATE 0 bits indicate the decimation ratio used. Table 10 is a truth table for the decimation rate bits.

**Table 10. Decimation Rate Status Bits**

Decimate	DEC_RATE 1	DEC_RATE 0
64x	0	1
128 <sup>1</sup> x	1	X
256x	0	0

<sup>1</sup>Don't care. If the DEC\_RATE 1 bit is set to 1, AD7764 is in Decimate 128x mode.

### READING STATUS AND OTHER REGISTERS

The AD7764 features a gain correction register, an overrange register, and a read-only status register. To read back the contents of these registers, the user must first write to the control register of the device, and set the bit that corresponds to the register to be read. The next read operation outputs the contents of the selected register (on the SDO pin) instead of a conversion result.

To ensure that the next read cycle contains the contents of the register written to, the write operation to that register must be completed a minimum of  $8 \times t_{\text{SCO}}$  before the falling edge of  $\overline{\text{FSO}}$ , which indicates the start of the next read cycle. See Figure 4 for further details.

The AD7764 Registers section provides more information on the relevant bits in the control register.

### WRITING TO THE AD7764

A write operation to the AD7764 is shown in Figure 3. The serial writing operation is synchronous to the SCO signal. The status of the frame synchronization input,  $\overline{\text{FSI}}$ , is checked on the falling edge of the SCO signal. If the  $\overline{\text{FSI}}$  line is low, then the first data bit on the serial data in (SDI) line is latched in on the next SCO falling edge.

Set the active edge of the  $\overline{\text{FSI}}$  signal to occur at a position when the SCO signal is high or low to allow setup and hold times from the SCO falling edge to be met. The width of the  $\overline{\text{FSI}}$  signal can be set to between 1 and 32 SCO periods wide. A second, or subsequent, falling edge that occurs before 32 SCO periods have elapsed, is ignored.

Figure 3 details the format for the serial data being written to the AD7764 through the SDI pin. Thirty-two bits are required for a write operation. The first 16 bits are used to select the register address that the data being read is intended for. The second 16 bits contain the data for the selected register.

Writing to the AD7764 is allowed at any time, even while reading a conversion result. Note that after writing to the devices, valid data is not output until after the settling time for the filter has elapsed. The FILTER-SETTLE status bit is asserted at this point to indicate that the filter has settled and that valid data is available at the output.

## AD7764 FUNCTIONALITY

### SYNCHRONIZATION

The  $\overline{\text{SYNC}}$  input to the AD7764 provides a synchronization function that allows the user to begin gathering samples of the analog front-end input from a known point in time.

The  $\overline{\text{SYNC}}$  function allows multiple AD7764s, operated from the same master clock, that use common  $\overline{\text{SYNC}}$  and  $\overline{\text{RESET}}$  signals to be synchronized so that each ADC simultaneously updates its output register.

Connect common MCLK,  $\overline{\text{SYNC}}$  and  $\overline{\text{RESET}}$  signals to all AD7764 devices in the system. On the falling edge of the  $\overline{\text{SYNC}}$  signal, the digital filter sequencer is reset to 0. The filter is held in a reset state until a rising edge of the SCO senses  $\overline{\text{SYNC}}$  high. Thus, to perform a synchronization of devices, a  $\overline{\text{SYNC}}$  pulse of a minimum of 2.5 ICLK cycles in length can be applied, synchronous to the falling edge of SCO. On the first rising edge of SCO after  $\overline{\text{SYNC}}$  goes logic high, the filter is taken out of reset, and the multiple parts gather input samples synchronously.

Following a  $\overline{\text{SYNC}}$ , the digital filter needs time to settle before valid data can be read from the AD7764. The user knows there is valid data on the SDO line by checking the FILTER-SETTLE status bit (see D7 in Table 9) that is output with each conversion result. The time from the rising edge of  $\overline{\text{SYNC}}$  until the FILTER-SETTLE bit asserts depends on the filter configuration used. See the Theory of Operation section and the values listed in Table 6 for details on calculating the time until FILTER-SETTLE asserts. Note that the FILTER\_SETTLE bit is designed as a reactionary flag to indicate when the conversion data output is valid.

### OVERRANGE ALERTS

The AD7764 offers an overrange function in both a pin and status bit output. The overrange alerts indicate when the voltage applied to the AD7764 modulator input pins exceeds the limit set in the overrange register, indicating that the voltage applied is approaching a level where the modulator will be overranged. To set this limit, the user must program the register. The default overrange limit is set to 80% of the  $V_{\text{REF}}$  voltage (see the AD7764 Registers section).

The OVERRANGE pin outputs logic high to alert the user that the modulator has sampled an input voltage greater in magnitude than the overrange limit as set in the overrange register. The OVERRANGE pin is set to logic high when the modulator samples an input above the overrange limit. Once the input returns below the limit, the OVERRANGE pin returns to zero. The OVERRANGE pin is updated after the first FIR filter stage. Its output changes at the ICLK/4 frequency.

The OVR status bit is output as Bit D6 on SDO during a data conversion, and can be checked in the AD7764 status register. This bit is less dynamic than the OVERRANGE pin output. It is updated on each conversion result output, that is, the bit

changes at the output data rate. If the modulator has sampled a voltage input that exceeded the overrange limit during the process of gathering samples for a particular conversion result output, then the OVR bit is set to logic high.

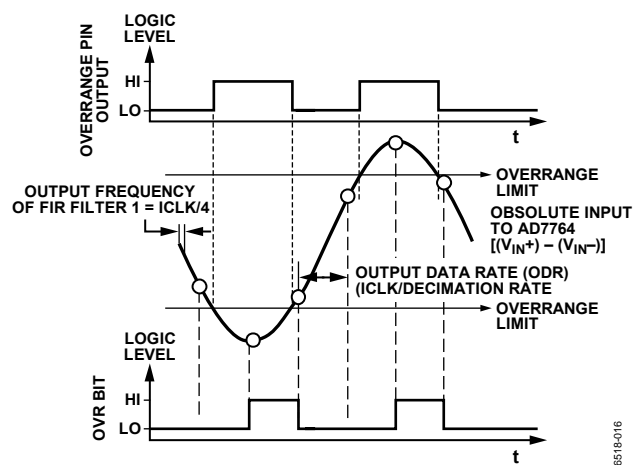


Figure 38. OVERRANGE Pin and OVR Bit vs. Absolute Voltage Applied to Modulator

The output points from FIR Filter 1 in Figure 38 are not drawn to scale relative to the output data rate points. The FIR Filter 1 output is updated either 16 $\times$ , 32 $\times$ , or 64 $\times$  faster than the output data rate depending on the decimation rate in operation.

### POWER MODES

During power-up, the AD7764 defaults to operate in normal power mode. There is no register write required.

The AD7764 also offers low power mode. To operate the device in low power mode, the user sets the LPWR bit in the control register to logic high (See Figure 39). Operating the AD7764 in low power mode has no impact on the output data rate or available bandwidth.

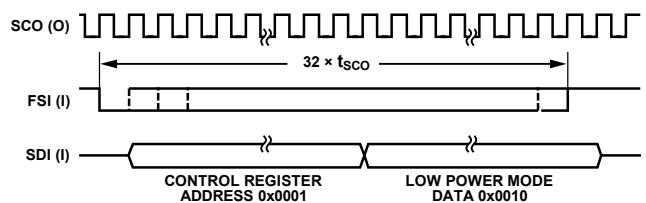


Figure 39. Write Scheme for Low Power Mode

The AD7764 features a  $\overline{\text{RESET/PWRDWN}}$  pin. Holding the input to this pin logic low places the AD7764 in power-down mode. All internal circuitry is reset. To utilize the  $\overline{\text{RESET}}$  functionality, pulse the input to this pin low for a minimum of one MCLK period. This action resets the internal circuitry. When the AD7764 receives a logic high input on the  $\overline{\text{RESET/PWRDWN}}$  pin, the device powers up.

# AD7764

## DECIMATION RATE PIN

The decimation rate of the AD7764 is selected using the DEC\_RATE pin. Table 11 shows the voltage input settings required for each of the three decimation rates.

Table 11 DEC\_RATE Pin Settings

Decimate	DEC_RATE Pin	Max Output Data Rate
64×	DVDD	312.5 kHz
128×	Floating	156.25 kHz
256×	GND	78.125 kHz

## DAISY CHAINING

Daisy chaining devices allows numerous devices to use the same digital interface lines. This feature is especially useful for reducing component count and wiring connections, such as in isolated multiconverter applications or for systems with a limited interfacing capacity. Data readback is analogous to clocking a shift register.

The block diagram in Figure 40 shows how to connect devices to achieve daisy-chain functionality. Figure 40 shows four AD7764 devices daisy-chained together with a common MCLK signal applied. This can only work in decimate 128× or 256× modes.

### READING DATA IN DAISY-CHAIN MODE

Referring to Figure 40, note that the SDO line of AD7764 (A) provides the output data from the chain of AD7764 converters. Also, note that for the last device in the chain, AD7764 (D), the SDI pin is connected to ground. All of the devices in the chain must use common MCLK and SYNC signals.

To enable the daisy-chain conversion process, apply a common SYNC pulse to all devices (see the Synchronization section).

After applying a SYNC pulse to all devices, the filter settling time must pass before the FILTER-SETTLE bit is asserted indicating valid conversion data at the output of the chain of devices. As shown in Figure 41, the first conversion result is output from the device labeled AD7764 (A). This 32-bit conversion result is then followed by the conversion results

from the devices AD7764 (B), AD7764 (C), and AD7764 (D), respectively with all conversion results output in an MSB first sequence. The signals output from the daisy chain are the stream of conversion results from the SDO pin of AD7764 (A) and the FSO signal output by the first device in the chain, AD7764 (A).

The falling edge of FSO signals the MSB of the first conversion output in the chain. FSO stays logic low throughout the 32 SCO clock periods needed to output the AD7764 (A) result and then goes logic high during the output of the conversion results from the devices AD7764 (B), AD7764 (C), and AD7764 (D).

The maximum number of devices that can be daisy-chained is dependent on the decimation rate selected. Calculate the maximum number of devices that can be daisy chained by simply dividing the chosen decimation rate by 32 (the number of bits that must be clocked out for each conversion). Table 12 provides the maximum number of chained devices for each decimation rate.

**Table 12. Maximum Chain Length for all Decimation Rates**

Decimation Rate	Maximum Chain Length
256×	8
128×	4
64×	2

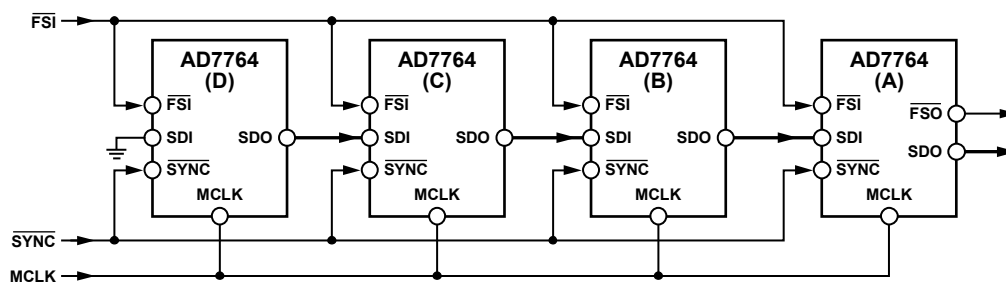


Figure 40. Daisy-Chaining Four Devices in Decimate 128× Mode Using a 40 MHz MCLK Signal

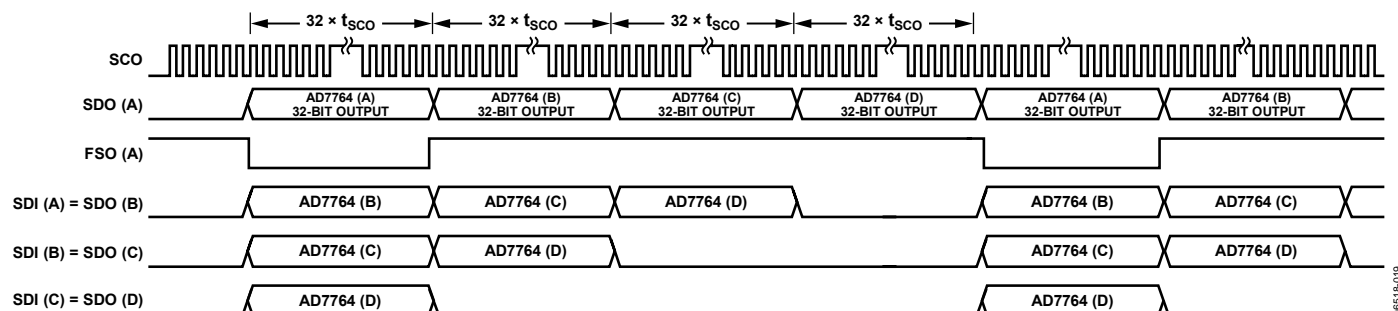


Figure 41. Daisy-Chain Mode, Data Read Timing Diagram  
(for Daisy-Chain Configuration Shown in Figure 40)

## WRITING DATA IN DAISY-CHAIN MODE

Writing to AD7764 devices in daisy-chain mode is similar to writing to a single device. The serial writing operation is synchronous to the SCO signal. The status of the frame synchronization input,  $\overline{\text{FSI}}$ , is checked on the falling edge of the SCO signal. If the  $\overline{\text{FSI}}$  line is low, then the first data bit on the serial data in the SDI line is latched in on the next SCO falling edge.

Writing data to the AD7764 in daisy-chain mode operates with the same timing structure as writing to a single device (see Figure 3). The difference between writing to a single device and writing to a number of daisy-chained devices is in the implementation of the  $\overline{\text{FSI}}$  signal. The number of devices that are in the daisy chain determines the period for which the  $\overline{\text{FSI}}$  signal must remain logic low. To write to  $n$  number of devices in the daisy chain, the period between the falling edge of  $\overline{\text{FSI}}$  and the

rising edge of  $\overline{\text{FSI}}$  must be between  $32 \times (n-1)$  to  $32 \times n$  SCO periods. For example, if three AD7764 devices are being written to in daisy-chain mode,  $\overline{\text{FSI}}$  is logic low for between  $32 \times (3-1)$  to  $32 \times 3$  SCO pulses. This means that the rising edge of  $\overline{\text{FSI}}$  must occur between the 64<sup>th</sup> and 96<sup>th</sup> SCO period.

The AD7764 devices can be written to at any time. The falling edge of  $\overline{\text{FSI}}$  overrides all attempts to read data from the SDO pin. In the case of a daisy chain, the  $\overline{\text{FSI}}$  signal remaining logic low for more than 32 SCO periods indicates to the AD7764 device that there are more devices further on in the chain. This means the AD7764 directs data that is input on the SDI pin to its SDO pin. This ensures that data is passed to the next device in the chain.

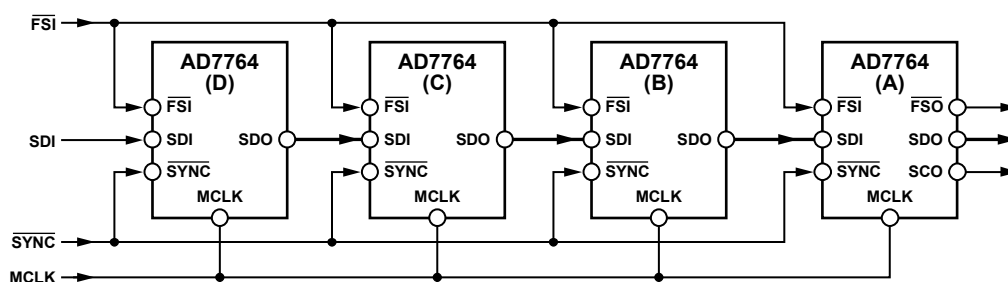


Figure 42. Writing to AD7764 Daisy-Chain Configuration

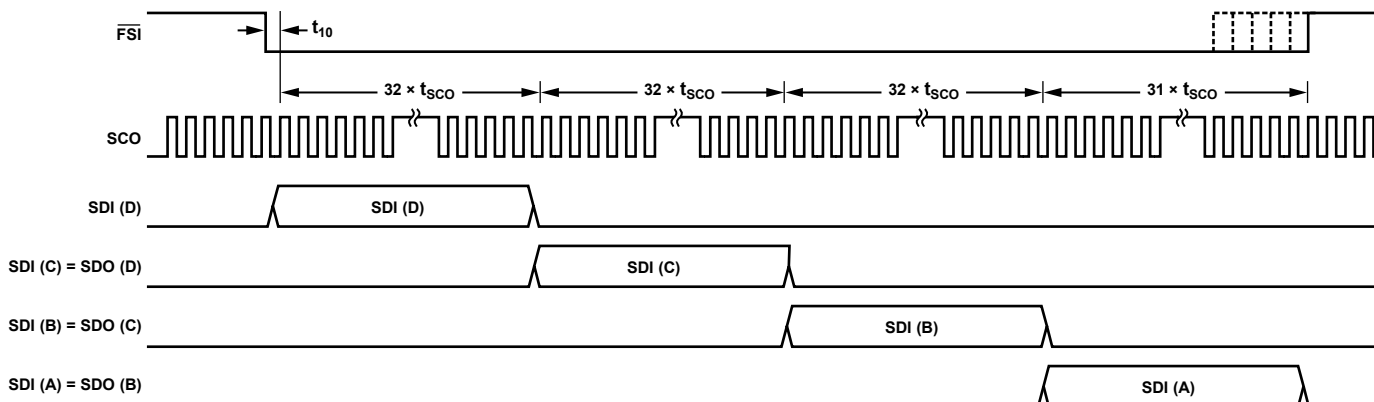


Figure 43. Daisy-Chain Write Timing Diagram; Writing to Four AD7764 Devices



## CLOCKING THE AD7764

The AD7764 requires an external low jitter clock source. This signal is applied to the MCLK pin. An internal clock signal (ICLK) is derived from the MCLK input signal. The ICLK controls the internal operation of the AD7764. The maximum ICLK frequency is 20 MHz. To generate the ICLK

$$ICLK = MCLK/2$$

For output data rates equal to those used in audio systems, a 12.288 MHz ICLK frequency can be used. As shown in Table 6, output data rates of 96 kHz and 48 kHz are achievable with this ICLK frequency.

### MCLK JITTER REQUIREMENTS

The MCLK jitter requirements depend on a number of factors and are given by

$$t_{j(rms)} = \frac{\sqrt{OSR}}{2 \times \pi \times f_{IN} \times 10 \frac{SNR(dB)}{20}}$$

where:

$OSR$  = oversampling ratio =  $f_{ICLK}/ODR$ .

$f_{IN}$  = maximum input frequency.

$SNR(dB)$  = target SNR.

#### Example 1

This example can be taken from Table 6, where:

$ODR = 312.5$  kHz.

$f_{ICLK} = 20$  MHz.

$f_{IN}(\text{max}) = 156.25$  kHz.

$SNR = 104$  dB.

$$t_{j(rms)} = \frac{\sqrt{64}}{2 \times \pi \times 156.25 \times 10^3 \times 10^{5.2}} = 51.41 \text{ ps}$$

This is the maximum allowable clock jitter for a full-scale, 156.25 kHz input tone with the given ICLK and output data rate.

#### Example 2

Take a second example from Table 6, where:

$ODR = 48$  kHz.

$f_{ICLK} = 12.288$  MHz.

$f_{IN}(\text{max}) = 19.2$  kHz.

$SNR = 109$  dB.

$$t_{j(rms)} = \frac{\sqrt{256}}{2 \times \pi \times 19.2 \times 10^3 \times 10^{5.45}} = 470 \text{ ps}$$

The input amplitude also has an effect on these jitter figures. For example, if the input level is 3 dB below full-scale, the allowable jitter is increased by a factor of  $\sqrt{2}$ , increasing the first example to 57.75 ps rms. This happens when the maximum slew rate is decreased by a reduction in amplitude.

Figure 44 and Figure 45 illustrate this point, showing the maximum slew rate of a sine wave of the same frequency, but with different amplitudes.

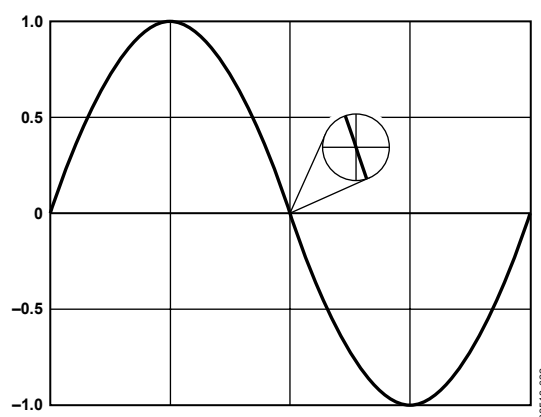


Figure 44. Maximum Slew Rate of Sine Wave with Amplitude of 2 V p-p

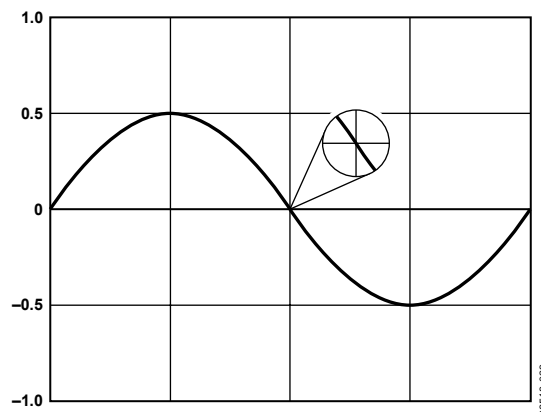


Figure 45. Maximum Slew Rate of Same Frequency Sine Wave with Amplitude of 1 V p-p

## DECOUPLING AND LAYOUT INFORMATION

### SUPPLY DECOUPLING

The decoupling of the supplies applied to the AD7764 is important in achieving maximum performance. Each supply pin must be decoupled to the correct ground pin with a 100 nF, 0603 case size capacitor.

Pay particular attention to decoupling Pin 7 ( $AV_{DD2}$ ) directly to the nearest ground pin (Pin 8). The digital ground pin AGND2 (Pin 20) is routed directly to ground. Also, connect REFGND (Pin 26) directly to ground.

The  $DV_{DD}$  (Pin 17) and  $AV_{DD3}$  (Pin 28) supplies should be decoupled to the ground plane at a point away from the device.

It is advised to decouple the supplies that are connected to the following supply pins through 0603 size, 100 nF capacitors to a star ground point linked to Pin 23 (AGND1):

- $V_{REF+}$  (Pin 27)
- $AV_{DD4}$  (Pin 25)
- $AV_{DD1}$  (Pin 24)
- $AV_{DD2}$  (Pin 21)

A layout decoupling scheme for the these supplies, which connect to the right hand side of the AD7764, is shown in Figure 46. Note the star-point ground created at Pin 23.

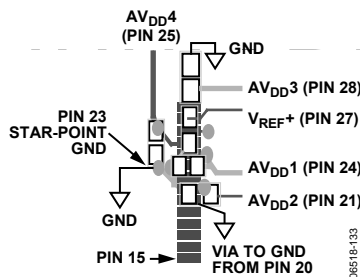


Figure 46. Supply Decoupling

### REFERENCE VOLTAGE FILTERING

A low noise reference source, such as the ADR444 or ADR34 (4.096 V), is suitable for use with the AD7764. The reference voltage supplied to the AD7764 should be decoupled and filtered as shown in Figure 47.

The recommended scheme for the reference voltage supply is a 200  $\Omega$  series resistor connected to a 100  $\mu$ F tantalum capacitor, followed by a 10 nF decoupling capacitor very close to the  $V_{REF+}$  pin.

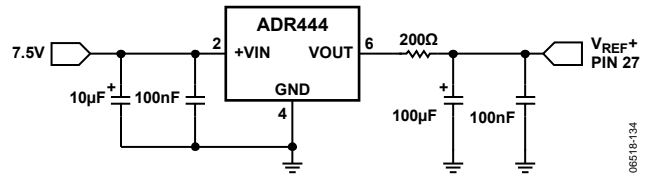


Figure 47. Reference Connection

### DIFFERENTIAL AMPLIFIER COMPONENTS

The components recommended for use around the on-chip differential amplifier are detailed in Table 7. Matching the components on both sides of the differential amplifier is important to minimize distortion of the signal applied to the amplifier. A tolerance of 0.1% or better is required for these components. Symmetrical routing of the tracks on both sides of the differential amplifier also assists in achieving stated performance. Figure 48 shows a typical layout for the components around the differential amplifier. Note that the traces for both differential paths are made as symmetrical as possible and the feedback resistors and capacitors are placed on the underside of the PCB to enable the simplest routing.

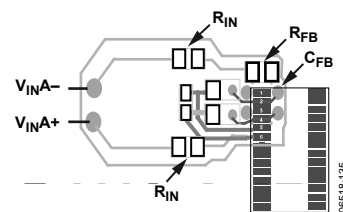


Figure 48. Typical Layout Structure for Surrounding Components

### LAYOUT CONSIDERATIONS

While using the correct components is essential to achieve optimum performance, the correct layout is equally as important. The AD7764 product page on [www.analog.com](http://www.analog.com) contains the Gerber files for the AD7764 evaluation board. The Gerber files should be used as a reference when designing any system using the AD7764.

The use of ground planes should be carefully considered. To ensure that the return currents through the decoupling capacitors are flowing to the correct ground pin, the ground side of the capacitors should be as close to the ground pin associated with that supply as recommended in the Supply Decoupling section.

## USING THE AD7764

Step 1 through Step 5 detail the sequence for powering up and using the AD7764.

1. Apply power to the device.
2. Start the clock oscillator, applying MCLK.
3. Take  $\overline{\text{RESET}}$  low for a minimum of one MCLK cycle.
4. Wait a minimum of two MCLK cycles after  $\overline{\text{RESET}}$  has been released.
5. If multiple parts are being synchronized, a  $\overline{\text{SYNC}}$  pulse must be applied to the parts. Otherwise, no  $\overline{\text{SYNC}}$  pulse is required.

When applying the  $\overline{\text{SYNC}}$  pulse

- The application of a  $\overline{\text{SYNC}}$  pulse to the device must not coincide with a write to the device.
- Ensure that the  $\overline{\text{SYNC}}$  pulse is taken low for a minimum of 2.5 ICLK cycles.

Data can then be read from the device using the default gain and overrange threshold values. The conversion data read is not valid, however, until the settling time of the filter has elapsed. Once this has occurred, the FILTER-SETTLE status bit is set indicating that the data is valid.

Values for gain and overrange thresholds can be written to or read from the respective registers at this stage.

## BIAS RESISTOR SELECTION

The AD7764 requires a resistor to be connected between the  $R_{\text{BIAS}}$  and AGND pins. The resistor value should be selected to give a current of 25  $\mu\text{A}$  through the resistor to ground. For a 4.096 V reference voltage, the correct resistor value is 160 k $\Omega$ .

# AD7764

## AD7764 REGISTERS

The AD7764 has a number of user-programmable registers. The control register is used to set the functionality of the on-chip buffer and differential amplifier and provides the option to power down the AD7764. There are also digital gain and overrange threshold registers. Writing to these registers involves writing the register address followed by a 16-bit data word. The register addresses, details of individual bits, and default values are provided in this section.

### CONTROL REGISTER

Table 13. Control Register (Address 0x0001, Default Value 0x0000)

MSB														LSB	
D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
0	RD OVR	RD GAIN	0	RD STAT	0	SYNC	0	BYPASS REF	0	0	0	PWR DOWN	LPWR	REF BUF OFF	AMP OFF

Table 14. Bit Descriptions of Control Register

Bit	Mnemonic	Comment
14	RD OVR <sup>1,2</sup>	Read Overrange. If this bit is set, the next read operation outputs the contents of the overrange threshold register instead of a conversion result.
13	RD GAIN <sup>1,2</sup>	Read Gain. If this bit is set, the next read operation outputs the contents of the digital gain register.
11	RD STAT <sup>1,2</sup>	Read Status. If this bit is set, the next read operation outputs the contents of the status register.
9	SYNC <sup>1</sup>	Synchronize. Setting this bit initiates an internal synchronization routine. Setting this bit simultaneously on multiple devices synchronizes all filters.
7	BYPASS REF	Bypass Reference. Setting this bit bypasses the reference buffer if the buffer is off.
3	PWR DOWN	Power Down. A logic high powers the device down without resetting. Writing a 0 to this bit powers the device back up.
2	LPWR	Low Power Mode. Set to Logic 1 when AD7764 is in low power mode.
1	REF BUF OFF	Reference Buffer Off. Asserting this bit powers down the reference buffer.
0	AMP OFF	Amplifier Off. Asserting this bit switches the differential amplifier off.

<sup>1</sup> Bit 14 to Bit 11 and Bit 9 are self-clearing bits.

<sup>2</sup> Only one of the bits can be set in any write operation because it determines the contents of the next read operation. \_ \_ \_ \_ \_

### STATUS REGISTER

Table 15. Status Register (Read Only)

MSB														LSB	
D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
PARTNO	1	0	0	0	FILTER-SETTLE	0	OVR	0	1	0	REF BUF ON	AMP ON	LPWR	DEC 1	DEC 0

Table 16. Bit Descriptions of Status Register

Bit	Mnemonic	Comment
15	PARTNO	Part Number. This bit is set to one for the AD7764.
10	FILTER-SETTLE	Filter Settling Bit. This bit corresponds to the FILTER-SETTLE bit in the status word output in the second 16-bit read operation. It indicates when data is valid.
9	0	Zero. This bit is set to Logic 0.
8	OVR	Overrange. If the current analog input exceeds the current overrange threshold, this bit is set.
4	REF BUF ON	Reference Buffer On. This bit is set when the reference buffer is in use.
3	AMP ON	Amplifier On. This bit is set when the input amplifier is in use.
2	LPWR	Low power mode. This bit is set when operating in low power mode.
1 to 0	DEC[1:0]	Decimation Rate. These bits correspond to decimation rate in use.

**GAIN REGISTER—ADDRESS 0x0004*****Non-Bit-Mapped, Default Value 0xA000***

The gain register is scaled such that 0x8000 corresponds to a gain of 1.0. The default value of this register is 1.25 (0xA000). This results in a full-scale digital output when the input is at 80% of  $V_{REF}$ , tying in with the maximum analog input range of  $\pm 80\%$  of  $V_{REF}$  p-p.

**OVERRANGE REGISTER—ADDRESS 0x0005*****Non-Bit-Mapped, Default Value 0xCCCC***

The overrange register value is compared with the output of the first decimation filter to obtain an overload indication with minimum propagation delay. This is prior to any gain scaling. The default value is 0xCCCC, which corresponds to 80% of  $V_{REF}$  (the maximum permitted analog input voltage). Assuming  $V_{REF} = 4.096$  V, the bit is then set when the input voltage exceeds approximately 6.55 V p-p differential. The overrange bit is set immediately if the analog input voltage exceeds 100% of  $V_{REF}$  for more than four consecutive samples at the modulator rate.

## OUTLINE DIMENSIONS

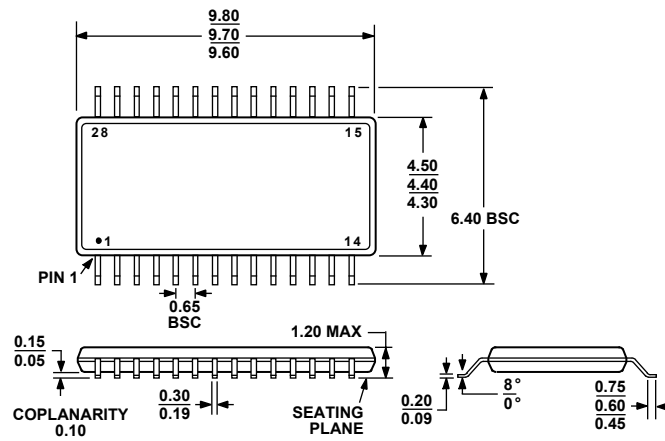


Figure 49. 28-Lead Thin Shrink Small Outline [TSSOP]  
(RU-28)  
Dimensions shown in millimeters

## ORDERING GUIDE

Model	Temperature Range	Package Description	Package Option
AD7764BRUZ <sup>1</sup>	–40°C to +85°C	28-Lead Thin Shrink Small Outline [TSSOP]	RU-28
AD7764BRUZ-REEL7 <sup>1</sup>	–40°C to +85°C	28-Lead Thin Shrink Small Outline [TSSOP]	RU-28
EVAL-AD7764EBZ <sup>1</sup>		Evaluation Board	

<sup>1</sup> Z = RoHS Compliant Part.

NOTES

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**AD7764**

## NOTES