



Introduction

This application note describes the STEVAL-TSP001V1 demonstration board for the evaluation of a power over Ethernet (PoE) system used to transmit electrical power, along with data, to remote devices over a standard twisted-pair cable in an Ethernet network.

A complete power solution for Ethernet-connected powered devices is presented. The power supply fully complies with IEEE 802.3-2005 PoE specifications and delivers the rated output from any compliant source.

Example outputs of 3.3 V and 12 V are given in this document, but other requirements can easily be met by implementing small changes.

Key features

- Low profile, small size: 5"w x 1.5"d x 0.65"h (0.5" except RJ-45 Ethernet connectors)
- Complies with all IEEE 802.3-2005 (IEEE 802.3af) Power over Ethernet specifications
- Respects source limitations
- Does not pollute power source
- 1500 V isolated outputs eliminate ground loops
- Highest possible economical output power (total power at output approximately 10 W)
- Useful output voltages
 - 12 V @ 0.65 A output (7.8 W, loose tolerance)
 - 3.3 V @ 0.65 A output (2.145 W, tight tolerance)
- Increased cost-effectiveness due to SMT construction (through-hole connectors for ruggedness)

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1 Overview

The IEEE 802.3af specification is intended to greatly simplify the wiring to remote equipment by providing power over the same medium that carries the signal to/from the equipment. Applications that particularly benefit from this concept are security cameras, wireless access points, and internet telephones. Power wiring, with its associated conduit installation and licensed electrician fees, is eliminated. The wiring voltage is kept to a safe level, less than 60 volts DC. This voltage is not even applied to a connector until the downstream equipment is determined to be connected and asking for power. Lower voltage signaling is used to determine the need for power.

The cable voltage was selected so that existing 48 V telecom equipment could be used to supply the power without requiring DC-DC conversion. Careful consideration was given to existing communications wiring. Category 5 and 6 wiring and connectors can be used unmodified to carry power, if the current is limited to values that cannot cause overheating.

Category 5 and 6 cables contain extra wire pairs that are unused in the present Ethernet structure. These can be used to carry power (PSE^(a) Pinout Alternative B), or the signal-carrying twisted pairs themselves can carry power if center-tapped transformers are used to inject and recover DC current (PSE Pinout Alternative A).

For further safety, the powered device (PD) must present a “maintain power” signature. If the load is disconnected, the source cuts off power to the cable.

Isolation is required between the power source and the PD ground, if it exists. In some applications this is not an issue, such as in plastic-cased standalone Ethernet devices without external connections.

If external connections are required, the powered device's accessible metal must have a local ground to avoid hazards caused by lightning-induced ground jumps.

1.1 Limitations on available power

Voltage must be kept below 60 V to meet IEC60950 and other specifications' safety limits. The standard telecom battery voltage range is 44 V to 57 V.

Steady-state current must be kept under 350 mA to prevent excessive temperature rise in the wire and connectors. (Higher current, 400 mA for 50ms max, can be used for startup.)

The 802.3af specification permits only one power scheme per channel, either unused pair or simplex leads. Both schemes cannot be used together to increase available power.

Consequently, at low input voltage, a minimum power of only 15.4 W is available for any load (350 mA at 44 V).

The specification also requires operation with 20 ohms of cable and connector resistance, further limiting the minimum power available at the powered device input to 12.94 W.

The specification also requires that power of either polarity be accepted. A bridge rectifier with its forward drop loss further reduces input power. At 350 mA, a 1N4004 diode drops 0.7 volts. Loss in a bridge built of parts similar to these is 0.49 W, leaving only 12.45 W at the PD power supply input. At about 82% efficiency, the power converter can deliver no more than approximately 10 W.

a. PSE: power sourcing equipment

2 Powered device demonstration board

2.1 Design choices

The following points are considered as requirements for powered device supplies:

Input

Three inputs are provided; one for each of the two PoE powering schemes, and one additional input for lab test and demo purposes.

Output

There are two outputs which cover most applications.

1. Low voltage DC, tightly regulated and relatively ripple-free, for logic circuitry.
2. Relatively high voltage DC for relays, actuators, motors, lighting, etc. High precision is typically not required, nor is low ripple.

Selected voltages and currents:

- 3.3 V at 0.65 A, ripple less than 50 mV P-P
- 12 V at 0.65 A, ripple in the range of 250 mV P-P

The 12 V output is cross-regulated from the 3.3 V output. It will maintain ± 10 to $\pm 15\%$ regulation.

1500 V isolation of the output is included because it is usually required and is easy to eliminate for additional small cost savings. Where appropriate, the demo board uses 2 mm clearance between the Ethernet input and circuitry that may need to be grounded locally.

Power over Ethernet interface

The ST STHS4257 power over Ethernet interface controller was chosen for the signature, classification, source connect, and converter start functions. This chip combines these functions in a small SO-8 package.

DC-DC Converter

The converter accepts, at a low cost, a wide range of input voltage and load currents.

Topology, operating mode, and control scheme

The converter uses the flyback topology. It is the simplest, lowest cost solution at the 10 W power level. It also supports multiple cross-regulated outputs at minimum possible cost.

Transition mode is used to maximize transformer utilization and minimize electro-magnetic interference (EMI). The converter starts each transformer charge cycle (transistor on) immediately after the output diodes shut off. There are no stability problems over 50% duty because there is no energy left in the transformer at the end of each cycle.

The converter uses peak current-mode control, in which the error between output and setpoint controls the peak current in the transformer primary.

Enable

It was decided to use the Power Good signal from the STHS4257 to start the converter. This ensures that the converter's input capacitor is fully charged well before the converter is allowed to start. If the converter was started from its own input voltage, there would be a coordination problem to be solved - the converter could start before the input capacitors were charged if conditions were incorrect. The cost is only a resistor and a PNP transistor, but the benefits include peace of mind.

Control chip

ST's L6565 quasi-resonant SMPS controller allows easy implementation of the transition mode peak current control scheme. It was designed for line voltage, but it can operate at much lower voltages with minor changes in the startup circuitry. The benefits include lower EMI and much lower turn-on losses than any other scheme.

Operating frequency

Because the L6565 operates in transition mode, it operates at variable frequency. The frequency is lowest at high output current and minimum input voltage. The converter is designed to operate at about 30 kHz under full load at 36 V input. The transformer is designed to go into saturation at a slightly lower frequency, and run at a higher frequency with a higher input voltage and lighter loads.

If a fixed operating frequency is required, this is NOT the recommended method. In some applications, the power supply must be synchronized with other circuitry so that its noise spikes occur between signal sampling times. In this case, another controller should be used.

Noise generated by the transition mode scheme is quite low, however. It is more than sufficient for the applications best suited for PoE technology.

Physical/mechanical

It was decided early on to keep the converter as small as possible consistent with the power requirements. SMT was a requirement, as was low profile

Early experiments with small surface-mount power transformers in the 10 W range required very high operating frequencies, in the 70 to 100 kHz range. The converters worked very well, but it was very difficult to keep the 2 mm clearance required for the 1500 V isolation requirement. Safety considerations made it necessary to include two unused pins between the cable-connected side and the load side of the transformer. The smaller SMT bobbins available would not support the wire required for 10 W of output. The smallest 12-pin SMT bobbin available was finally chosen, and the transformer core that fit into it became the core of choice.

The transformer height became the limiting height for components. Parts selection then proceeded.

The final height was set at ½", including the 1/16" thickness of the PC board, but not including the RJ-45 connectors or their leads, or the terminal strips. These serve demonstration functions only.

The supply dimensions (with the above exclusions) give a volume of 4" x 1.5" x 0.5", or 3 in³. At 10 W output, power density is a respectable 3.3 W per in³, including the PoE functions.

Figure 1. Block diagram of demonstration board PSAL06-17 rev 2

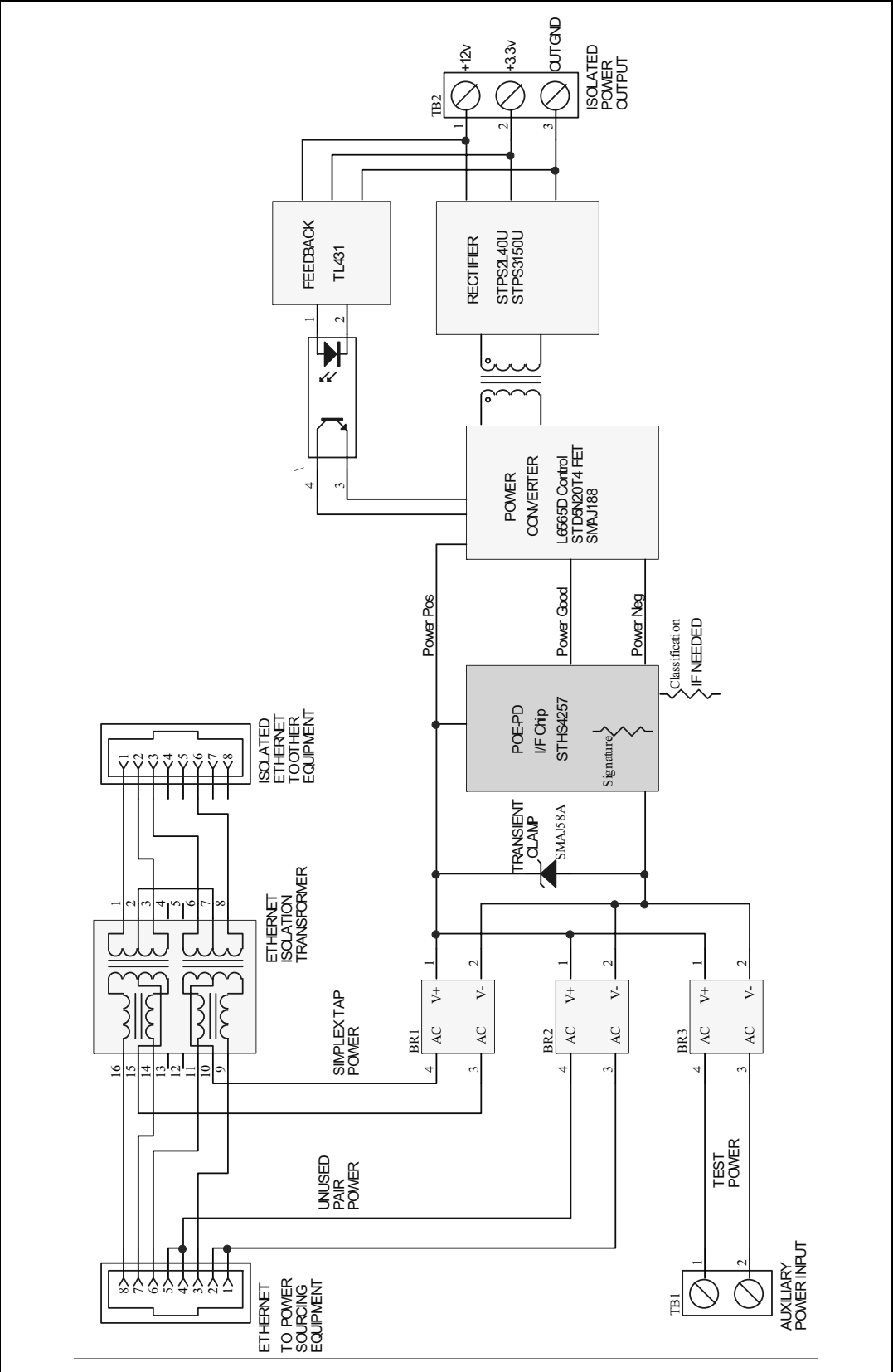


Figure 2. Front of demonstration board

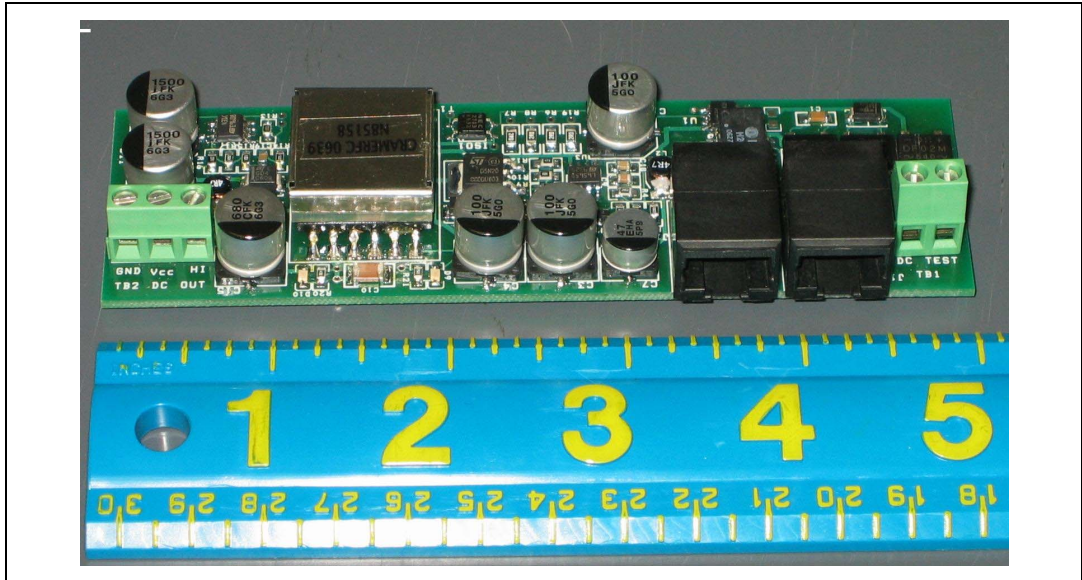


Figure 3. Rear of demonstration board

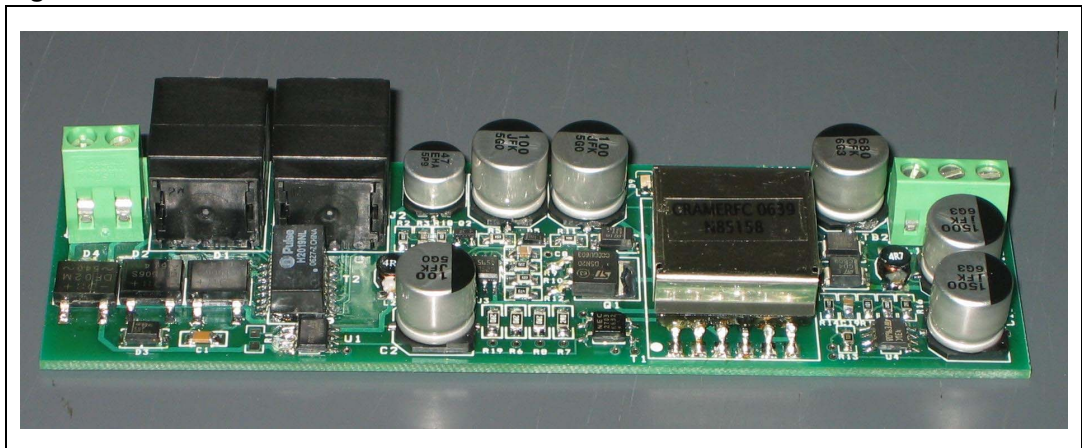
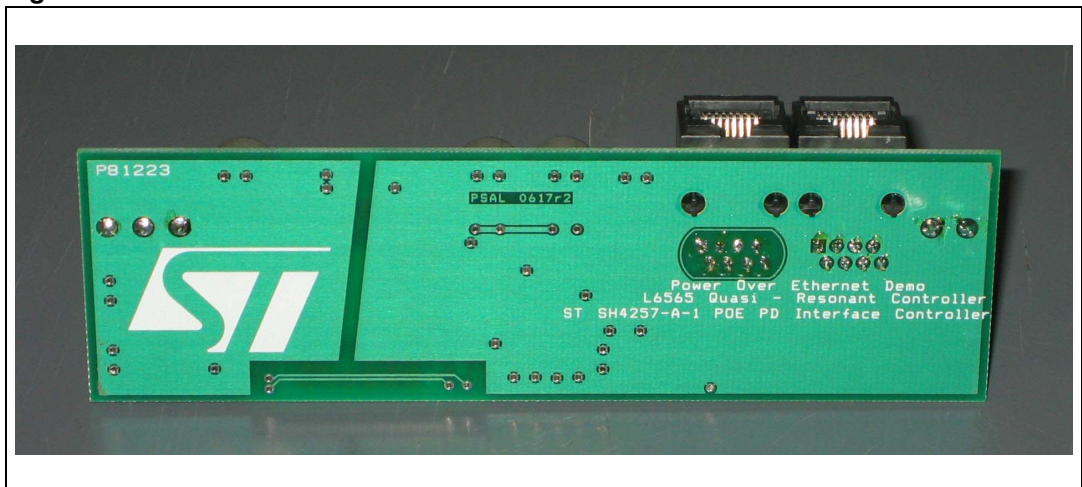
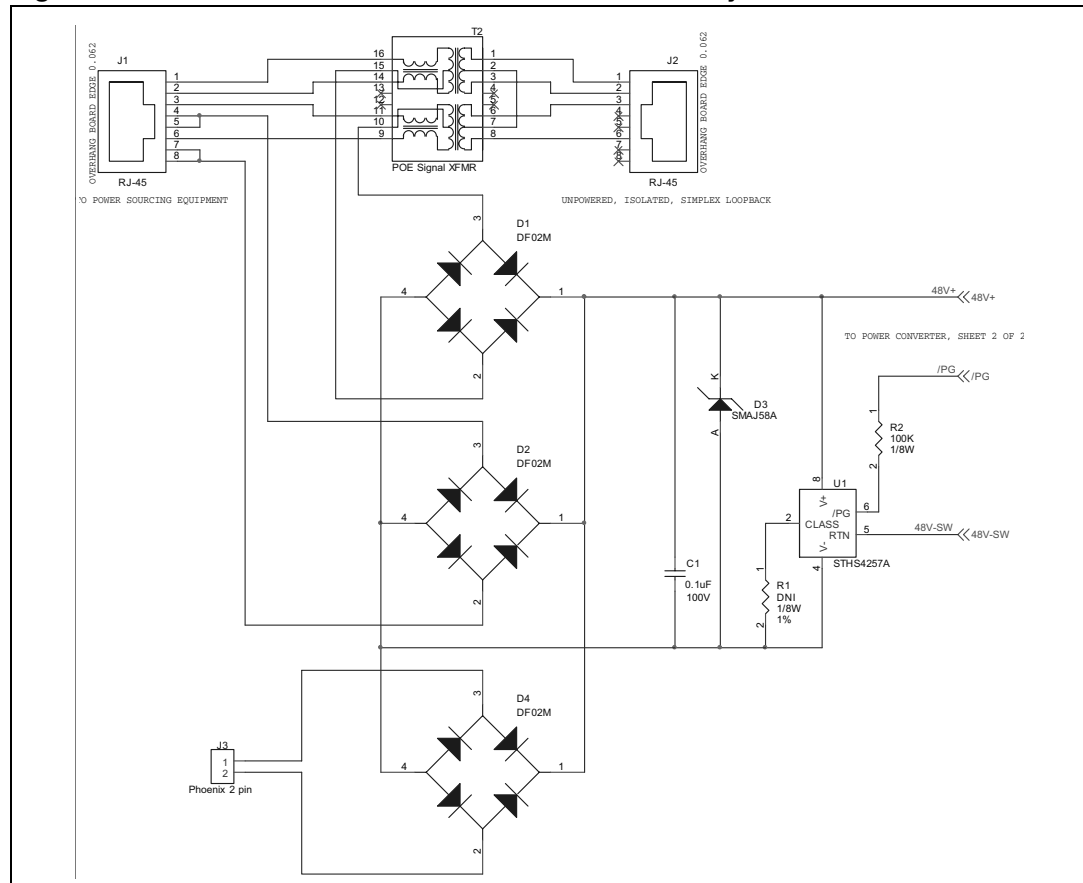


Figure 4. Bottom of demonstration board



3 Circuit descriptions

Figure 5. Test and Ethernet source connection circuitry



3.1 Inputs

3.1.1 Power supplies

There are three methods of powering the demonstration board:

1. Unused pairs (J1)
The unused twisted pairs in the Ethernet cable can carry power to RJ-45 pins 4 and 5, and pins 7 and 8.
2. Simplex leads (J1)
The transformer windings are center tapped, and power is carried over the same pairs as the signal leads. The DC power current balances out in the transformer - saturation of the core does not occur, and the signals can pass. Power is drawn off the centertaps (simplex leads) and signals are coupled to another winding.
3. Auxiliary DC input (TB1)
For convenience, this input method is provided for test and evaluation. Each input is sent through its own bridge rectifier so that it is polarity insensitive.

3.1.2 Transient protection

A 58 V Zener diode (D3) is placed across the DC bus so that it clamps all inputs to slightly more than that value. ESD and connection transients then cannot harm downstream circuitry.

3.1.3 Input capacitor

The 802.3af specification requires at least 0.05 μF of capacitance for the maintain power signature. 0.1 μF is installed at C1. This capacitor must be rated for at least 90 volts.

3.2 STHS4257 powered device interface controller

3.2.1 Sequence of operation

During startup (connection of PD or power-up of a PSE output), a reduced input voltage is used to identify the loads requiring power. Between -2.8 V and -10 V, an incremental load slope of 25 k indicates that the load is requesting power. This is called the PoE signature resistance.

3.2.2 POE Signature resistance

The STHS4257 powered device interface controller generates the 25 k Ω signature resistance slope internally. No external resistor is required. Note that there is a Signature Disable function on the chip, which is not used in this design. The signature disable function can be used to disable power from the PSE if the powered device is receiving its power from another source.

3.2.3 Classification

Between -15.5 and -20 V the load current indicates a power classification. Optionally, the Powered Device can inform the power sourcing equipment (PSE) to expect loading in a defined range. A precision resistor could be added at the R1 location to set Classification Current. The resistor was not installed in the demo board, so the board reports Class 0 (zero), informing the PSE that power may be required over any part of the full 0.44 W to 12.95 W load range. Table 3 in the STHS4257 datasheet and Tables 33-3 and 33-4 in the IEEE 803.2af specification show the defined ranges and resistor values. [Table 1](#) below combines the information.

Table 1. Power classes and class identification

Class	Power range	Notes	Classification current	R1 value
0	0.44 to 12.95 W	Default	0 to 4 mA	Open
1	0.44 to 3.84 W	Optional	9 to 12 mA	124 Ω
2	3.84 to 6.49 W	Optional	17 to 20 mA	68.1 Ω
3	6.49 to 12.95 W	Optional	26 to 30 mA	45.3 Ω
4	Reserved	Reserved	36 to 44 mA	30.9 Ω

Two methods of determining the classification are supported:

- Voltage between -15.5 and -20 V is applied and the current is measured (IEEE803.2af compliant); or,
- Current is applied and voltage measured (obsolete, requires multiple test currents).

The STHS4257 supports both methods -- it acts as a current sink. If voltage is applied and current measured, the classification is determined in a single step.

If a current between the classification ranges is applied, the voltage across the device will be either less than 15.5 V or greater than 20 V. Stepping the current between ranges allows determining the classification.

Because of the relatively high dissipation in the chip at the higher classes, the classification time is specified by IEEE 802.3af at 75 ms (maximum).

3.2.4 Startup sequence

If the signature (and classification, if implemented) tests indicate that power should be applied to the PD, the PSE will apply the available voltage to the ethernet cable with the current limited to 400 mA. (If the source is in current limit for more than 50ms, the load is disconnected.) This allows charging of the power converter input capacitors.

Action of the PD is then determined by the voltage at the STHS4257 input and the state of its internal current limiter.

If the input voltage to the STHS4257 is below 30 V, nothing happens; no current is supplied to the power converter.

If the input voltage is above 42 V, the STHS4257 turns on, supplying current-limited power to the power converter input.

The power converter requires capacitance at its input, usually in the range from 50 to 300 μ F. This capacitance (C2, 3, and 4) is charged to the input voltage by the internal current limiter of the STHS4257.

When the capacitor charging current falls to a predetermined value, the capacitor is assumed to be charged. At this point, input and output voltages of the STHS4257 are nearly equal, and the current limit function is replaced by a low-resistance switch.

When the switch turns on, the /Power Good signal is also turned on, pulling pin 6 to V_{OUT} . This signal is used to start the power converter.

Two events can stop the STHS4257 startup: overtemperature and undervoltage. If either event occurs, the /Power Good signal goes high impedance (open circuit), and the FET connection from V_{IN} to V_{OUT} (pins 4 and 5) is opened.

If neither event occurs, the /Power Good signal turns on Q2, which enables current to trickle through R5 to charge C7 in the housekeeping supply of the power converter. Approximately 40 milliseconds later, C7 is charged to the L6565's startup voltage and the converter starts.

3.2.5 Maintain power signature (MPS)

The converter must maintain two signatures if the PSE is to continue supplying power:

- DC MPS - Current of at least 10 mAdc drawn from the PSE for 60 ms out of any 360 ms period. Dropouts cannot exceed 300 ms.
- AC MPS - Impedance less than 27 K at 500 Hz, >2.5 V test signal

The PSE can optionally ignore either the DC or AC MPS. The PD must present both.

3.3 Power converter operation

The following sections refer to the power converter schematic shown in [Figure 6](#).

ST's L6565 (U3) is a transition-mode peak-current controller that drives the FET (Q1) of a flyback converter in response to feedback signals from the converter output and a bootstrap winding.

An excellent description of the converter operation is available in the L6565 datasheet, with further detail in ST application note AN1326. Additional design examples are shown in application notes AN1376, AN1439, and AN2252. A design spreadsheet is also available. It is strongly recommended that the designer consult these resources.

3.3.1 Input filtering

The power converter has a discontinuous input current. The AC component of this current is supplied locally, by capacitors C3 and C4. C1 and L2 filter the input voltage so that the power source is not polluted.

3.3.2 Startup

When the converter initially starts, the L6565 controller (U3) runs from the charge on C7. This charge is quickly depleted, however, and a second power source must start before U3 starves.

One of T3's secondaries is used to bootstrap housekeeping power to the L6565. Pin 12 of Transformer T3 feeds R11 and D5 to provide enough current for normal operation.

At Q1's first turn-on, current begins to rise linearly (several microseconds) in T3's primary, pins 2 and 3. The current is sensed by the L6565 as the voltage drop across R6, 7, 8, 10, and 19. At the threshold set by the L6565 (more about this in [Section 3.3.3: Regulation](#)), the gate drive is removed and the magnetic field generated by T3's primary current is picked up by its secondaries, and fed to the capacitors C7, C11, C12, and C15. The cycle repeats as soon as the field stored in the transformer is depleted, repeating until the capacitors are charged to the desired voltages.

3.3.3 Regulation

Eventually (several milliseconds) the load capacitors charge to the desired voltages. The voltage on C11 is monitored by U4, and when U4 conducts sufficiently, it turns on optoisolator ISO1.

On the left side of the isolation barrier, ISO1 pulls down on U3's compensation node (pin 2).

Peak primary current is controlled directly by the error in output voltage of the 3.3 V output, and inversely by the input voltage. A higher input voltage means that the converter spends less time charging T3's inductance, resulting in a higher power output for the same peak current. This is compensated by U3's internal multiplier, which reduces the peak current setting for higher voltage inputs; so the system gain, current limit and operating point remain roughly constant.

Divider R3-R4 sets the voltage input to the L6565's multiplier, which is used to compensate for the faster transformer charge at high voltage. The voltage on pin 2, multiplied by (3 volts less the voltage on V_{FF}), sets the shutoff point for the primary ramp current.

The schematic diagram illustrates the internal circuitry of a PoE PSE module (EFD20-12). It features a power input section with a 48V input and a 48V output. The circuit includes a transformer (T3) for power conversion, a MOSFET (D5) for switching, and a diode (D6) for rectification. The output stage consists of a diode (D10) and a MOSFET (D7) driving an LED (LED_YEL_SMT0805). The circuit also includes a feedback loop with a diode (D8) and a MOSFET (D9). Various resistors (R1-R17) and capacitors (C1-C10) are used for timing, biasing, and filtering. The module is powered by a 48V input and provides a 48V output. The schematic is labeled with component values and part numbers, and includes a legend for the components.

3.3.4 Critical conduction operation

When close to or at full load, this converter operates on the boundary between continuous conduction and discontinuous conduction. The magnetic field in the transformer is allowed to completely collapse each cycle as the combined secondary currents drop to zero, then the FET is turned on (with zero or very low voltage on its drain) to begin charging the primary inductance.

The end-of-secondary-conduction point is detected at T3 pin 12. The voltage across the winding is slightly above the voltage on C7, and will suddenly drop down through zero and swing negative as the magnetic field in T3 collapses. This is detected by U3 pin 5 and used to start the next cycle by driving the gate of Q1. R12 and the input capacitance of U3 pin 5 provide a slight tunable delay.

3.3.5 Outputs

Transformer T3 feeds two Schottky rectifiers for the 3.3 V and 12 V outputs. Regulation of only the 3.3 V output is regarded as sufficient, as the 12 V output is seldom used for critical loads. Cross-regulation is sufficient.

3.3.6 Miscellaneous component functions

- T1 provides a small amount of common-mode filtering and isolates the Ethernet input and output connectors.
- R2 limits the base current to Q2.
- R18 insures that Q2 leakage is minimal if it is not being driven.
- R11 and C7 provide a small filter that removes the leakage spike when current transfers from the primary to the secondary.
- R9 prevents oscillation of Q1 due to trace and lead inductance. It also slows slightly Q1's turnoff transient, softening the noise-producing edges.
- C10 short-circuits switching noise current that could be coupled from the drain of Q1 through the transformer capacitance to output ground.
- L1 reduces ripple in the 3.3 V output to digital circuit requirements; less than 2% P-P, with C11 and C12.
- C15 filters the 12 V output. The ripple and spike noise on this output is relatively high; the output is still suitable for driving relays, downstream power converters, or illumination.
- R13 insures that ISO1's LED can completely turn off. If not present, the approximate ½ mA keep-alive current required by U4 would partially turn on the isolator.
- R14 limits the current into the isolator.
- R16 and R16 divide the 3.3 V output down to 2.495 V so U4 can compare that voltage to its reference.
- R15 and C19 stabilize the control loop by slowing down U4's response to error signals.
- D9 (yellow LED), powered by R21, indicates that the STHS4257 chip has passed power to the power converter.
- D10 (green LED), powered by R20, indicates that the power converter is up and running.

3.4 Transformer details

The transformer used in the STEVAL-TSP001V1 demo board is Cramer part number N85158. The secondary turns counts can be changed to accommodate other voltages if required. Please contact the manufacturer for more information.

- Construction:
 - Core: EFD20, any power material. Gap for 164 μH total primary inductance, pins 2 and 3 ($A_{\text{sub}} L = 63 \text{ nH/T}^2$)
 - Bobbin: Pin Shine EFD-20 12-pin SMT bobbin
- Windings:
 - Winding 1: 1/2 primary; 26 turns 28AWG; start pin 11; finish pin 3; tape 1 layer 1.5 mil Mylar
 - Winding 2: 3.3 V secondary; 6 turns 3x 28AWG, 1 strand per section, trifilar
 - a) Section A: start pin 5; finish pin 8
 - b) Section B: start pin 6; finish pin 9
 - c) Section C: start pin 5, finish pin 9
 - Winding 3: 3.3 V to 12 V secondary section; 14 turns 28AWG Start pin 7 finish pin 6
 - Tape 1 layer 1.5 mil Mylar
 - Winding 4: Bootstrap; 26 turns 32AWG; start pin 12; finish pin 1
 - Winding 5: 1/2 primary; 25 turns 28AWG; start pin 2; finish pin 11
 - Tape 2 layers 1.5 mil Mylar to protect windings

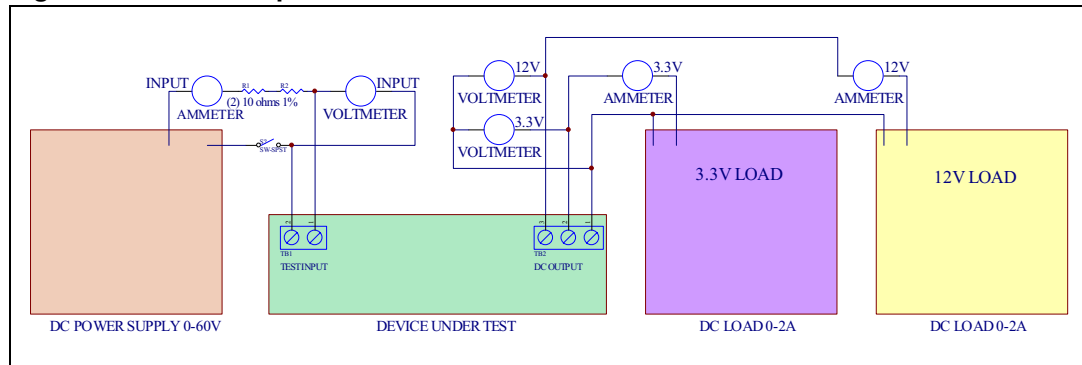
The transformer was overdesigned so that it could operate at higher power levels if required in the future.

4 Electrical characteristics

4.1 Test setup

Figure 7 shows a diagram of the loads and power supplies used for the test setup.

Figure 7. Test setup



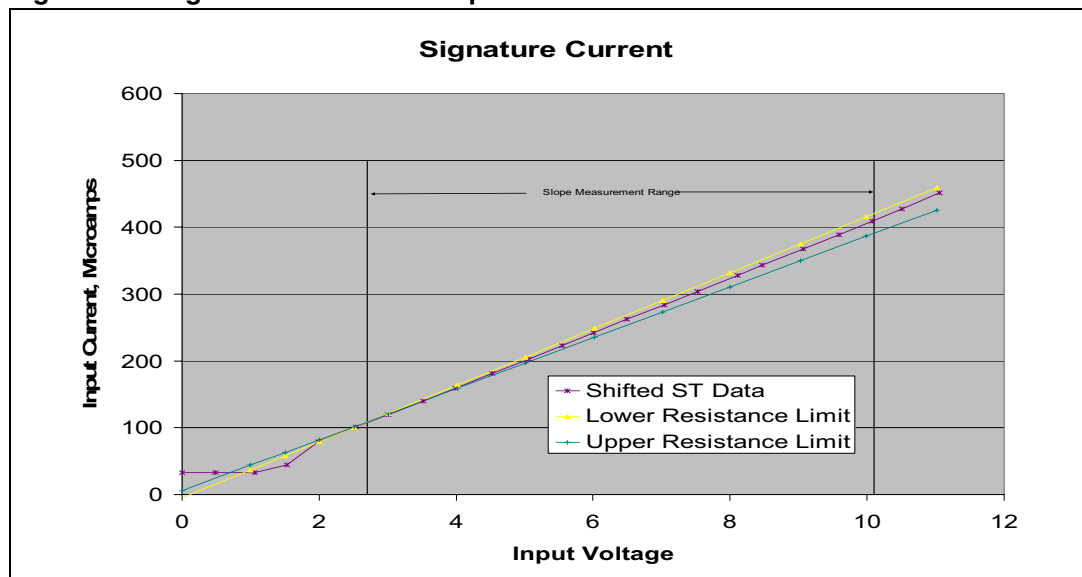
4.2 STHS4257 powered device interface controller

4.2.1 Signature current

Figure 8 compares the incremental slope and linearity of the signature resistance to the ideal slope and the limits. The limiting resistances were plotted, and then the limiting resistance curves and the data for the chip were shifted vertically to match the lower limit of the measurement range. Error can then be measured at the upper end of the measurement range.

Linearity of the slope does not appear to be an issue within the measurement range.

Figure 8. Signature resistance slopes



4.2.2 Classification current

[Table 2](#) shows the classification current for the values of classification resistors shown (R1 in [Figure 5](#)).

Table 2. Classification current

Class		0	1	2	3	4
Watts available at PSE connector		15.4 W	4.0 W	7.0 W	15.4 W	(future) Treat as class 0
Specified R		Open	124 Ω	68.1 Ω	45.3 Ω	30.9 Ω
Measured R used		Open	124.1 Ω	67.8 Ω	45.3 Ω	30.8 Ω
Specified current range		0 to 5 mA	8 to 13 mA	16 to 21 mA	25 to 31 mA	35 to 45 mA
STSH4257-A-1 test results	Current at 15.5 V	0.243 mA	10.11 mA	18.28 mA	27.22 mA	39.74 mA
	Current at 20.5 V	0.278 mA	10.15 mA	18.31 mA	27.25 mA	39.73 mA

All the currents are well within the specification limits.

4.2.3 Undervoltage lockout

The startup and shutdown voltages, at which the chip starts the load or turns the load off, were measured. Results are shown in [Table 3](#).

Table 3. PD Startup and shutdown voltages

Startup	Shutdown
37.01 V	31.9 V

These values are the board input voltages at which the STHS4257A1 chip enables and disconnects the power converter. The data was taken with no load on the power converter output. Startup occurs shortly after the /Power Good signal goes low, when the Vdd capacitor charges to the L6565's startup voltage (12.5 to 14.5 volts). Shutdown occurs when the STHS4257A1 chip disconnects the converter from its power source and the input capacitors discharge.

4.3 Powered device supply solution

The following properties were verified by testing the demonstration board against IEEE 802.3af, section 33.C.5 specifications.

4.3.1 Current draw at low input voltage

Table 4. Input current at 30V

Input voltage	Input current	Specification I_{\max}
30.0	0.273 mA	1.14 mA

The system is not allowed to draw significant power if its input is below 30 V.

4.3.2 Power Good signal and capacitor charging current

Figure 9. 42 V input

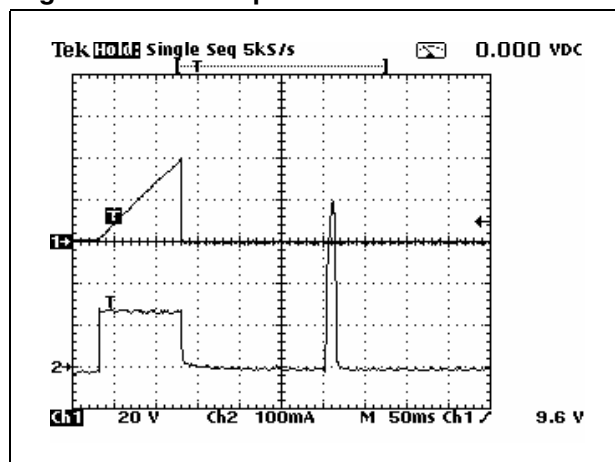
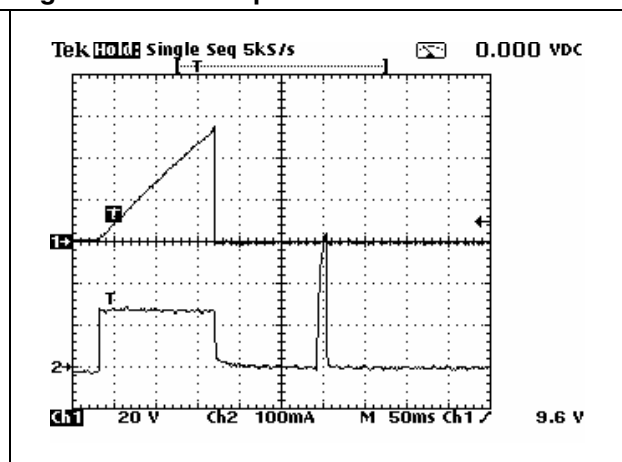


Figure 10. 57 V input



- Upper trace, channel 1: Power Good signal relative to power converter input negative
- Lower trace, channel 2: Input current to PD

4.3.3 Discussion

On the lower trace, two distinct regions are visible.

The first is the charging of the power converter input capacitors. The current is limited to a low value (around 140 mA) by the STHS4257A1 chip. After these capacitors charge, the Power Good (channel 1) signal drops, allowing the converter's Vcc capacitor to begin charging. A short time later, the converter starts, drawing significant current (approximately 350 mA) while it charges its output capacitors.

4.4 Startup loading on the power sourcing equipment

According to the specification, once power is applied to the PD, the PSE must shut down if the load current exceeds 400 mA for more than 50 milliseconds. After this startup transient, the overcurrent trip point is reduced to 350 mA.

The traces in [Figure 11](#) and [Figure 12](#) were taken with 20 ohms in series with the demo board's input to simulate cable resistance.

Figure 11. Full-load startup input current with cable resistance - 44 V source, 37 V at PD

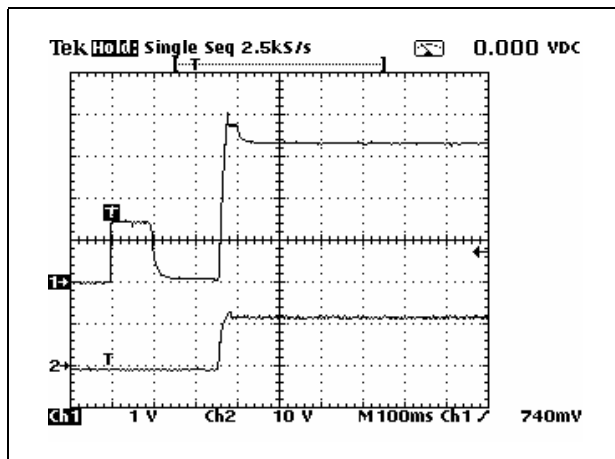
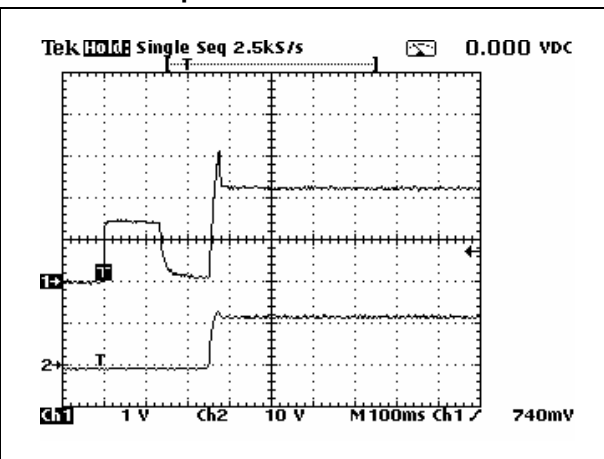


Figure 12. Full-load startup input current with cable resistance - 57 V source, input



- Channel 1: DC input current, 100 mA/division
- Channel 2: 12 V output voltage, 10 V/division

Starting at the first division from the left, note the capacitor charging current, limited by the STHS4257A1 chip. Until the power converter's input capacitors are charged, this chip does not permit the converter to start. This prevents the sudden application of both load current and capacitor charging current at the same time, which would overload the PSE.

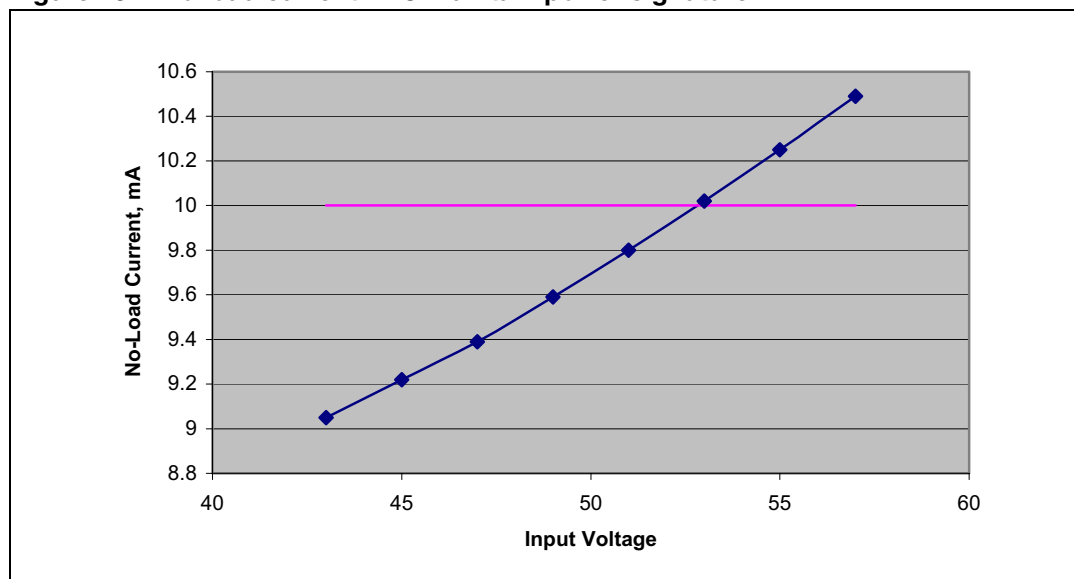
The STHS4257A1 chip dissipates considerable heat during the charging of the converter's input capacitors. It does rather well with the 300 μ F capacitance used in the demo board. Note that 300 μ F is a rather high value for the input capacitors, chosen to stress the chips. However, once the capacitors are charged, (and before the converter starts) the chip turns on an internal FET switch to reduce losses. Current limiting ceases; the converter is connected directly to the input power.

After about 3.5 divisions the power converter starts, drawing current from its input capacitors to charge its output capacitors and to supply the resistive test load. The energy required to charge the converter's output capacitors can be clearly seen as an overshoot in the input current (top trace).

Note also that the STHS4257A1 chip must supply input capacitor charging current for a longer period at 57 V, because it charges the capacitors to a higher voltage at the same current. The output capacitor charging spike is also shorter at 57 V, because more energy is stored in the input capacitors. Also note that the converter draws significantly less current at 57 V than it does at 37 V.

4.4.1 Maintain power signature

This design does not meet the DC maintain power signature current of 10 mA minimum. This could easily be corrected (if necessary) by increasing the LED current or preloading the outputs, but it is assumed that some load will be present at the converter's output. Input current with no load was measured over the operating voltage range.

Figure 13. No load current - DC maintain power signature

Note that most of the no-load current is due to the presence of the two LEDs on the board.

The AC maintain power signature is present by design. Small variations in input voltage will draw capacitive current from the PD's large input capacitors.

Both the DC and AC maintain power signatures must be present for compliance with the IEEE specification.

4.5 STHS4257A1 voltage drop under load

The load power was trimmed so that the input current was 350 mA and the voltage drop between the STHS4257-A-1 Vout (pin 5) and Vin (pin 4) was measured.

Table 5. Voltage drop under load, worst case input current

I _{DC} measured	V drop measured	Power loss
0.35 A	260 mV	91 mW

Discussion

This represents an efficiency loss of 0.61%, which is quite negligible.

4.6 Input current limit vs. input voltage

The STHS4257A1 chip limits the input current to 350 mA. The power converter current limit is set just slightly above that level, so that (if desired) the supply can be used at higher load currents with the source voltage at the high end of its range. At 350 mA and 57 V, with no Ethernet cable resistance present, the total input power available is almost 20 W.

The converter section's input current limit is flattened over the input voltage range by the voltage feed-forward scheme. See the L6565 literature for a thorough explanation.

4.7 Characteristics of entire system

4.7.1 Output vs. input voltage

As can be seen from the figures below, there is almost no sensitivity to input voltage. This is a characteristic common to all current-mode controlled converters.

4.7.2 Cross regulation

The following graphs should be self-explanatory.

Note that there is almost no variation with input voltage.

Figure 14. Cross regulation, 42 V In, 12 V at half load, 3.3 V load varied

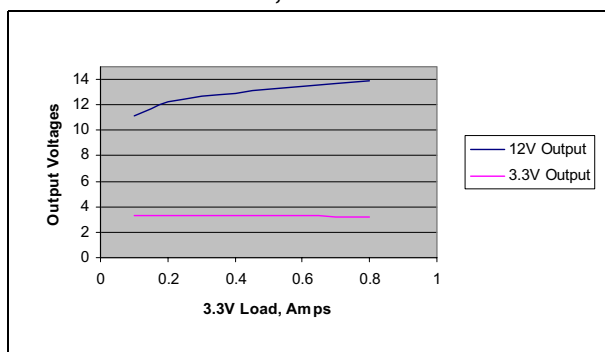


Figure 15. Cross regulation, 42 V In, 3.3 V at half load, 12 V load varied

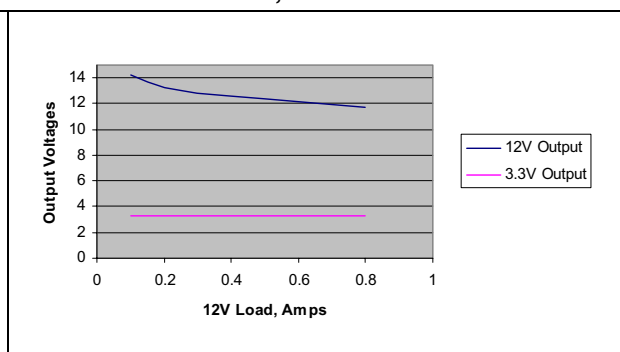


Figure 16. Cross regulation, 50 V In, 12 V at half load, 3.3 V load varied

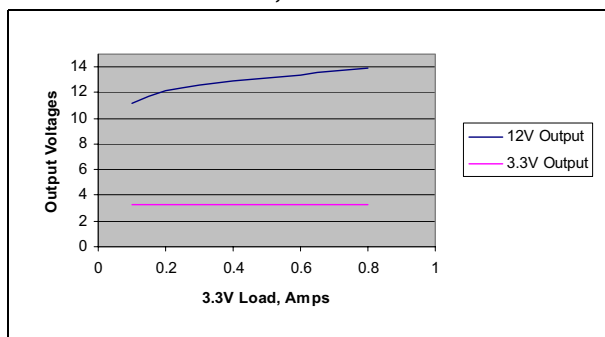


Figure 17. Cross regulation, 50 V In, 3.3 V at half load, 12 V load varied

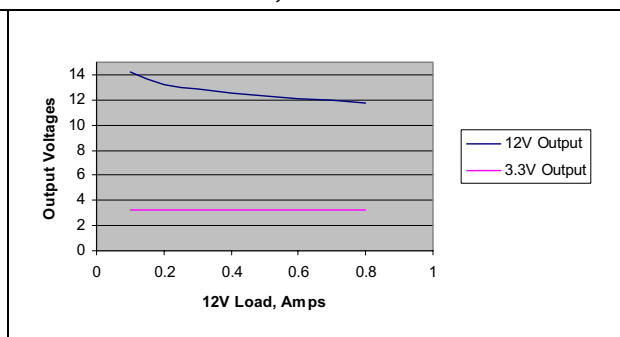


Figure 18. Cross regulation, 57 V In, 12 V at half load, 3.3 V load varied

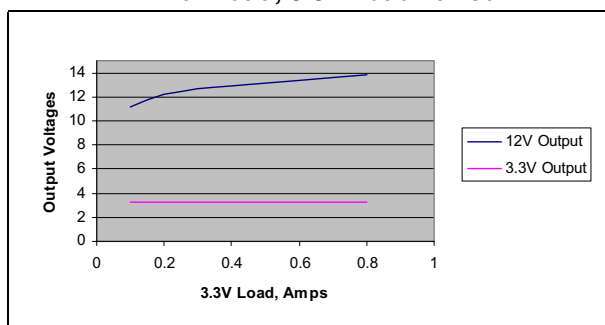
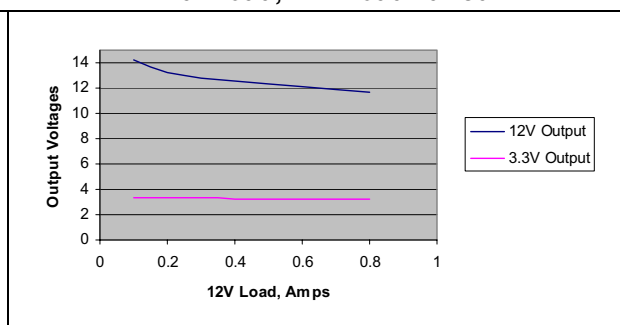


Figure 19. Cross regulation, 57 V In, 3.3 V at half load, 12 V load varied



The graphs above were run out to 0.8 A to show that loading can be traded off between the two outputs with very little effect on output voltage. Note, however, that at very light loads the cross regulation suffers. If light load operation is required, pre-loads may be necessary.

4.7.3 Startup and shutdown

Figure 20. 42 V full load startup

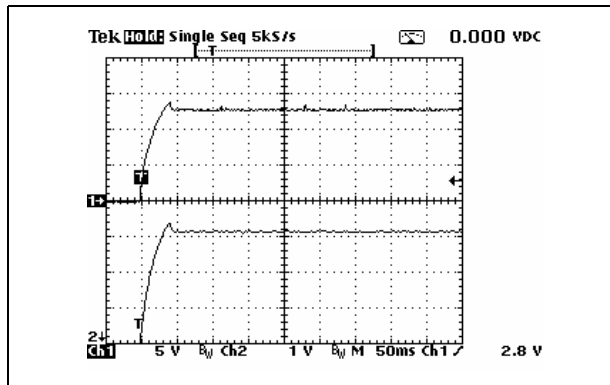
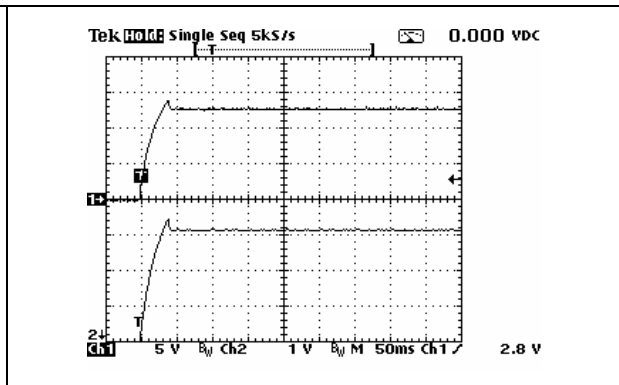


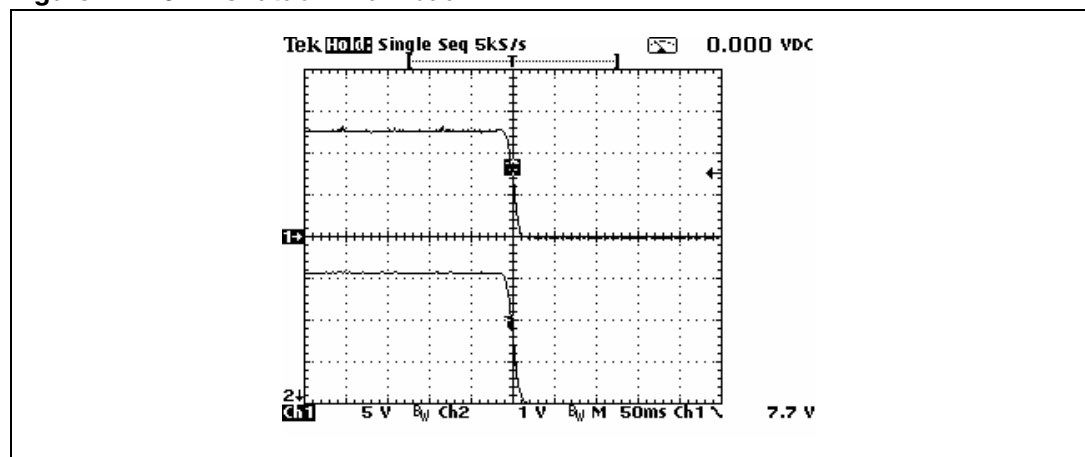
Figure 21. 57 V full load startup



- Channel 1 = 12 V output
- Channel 2 = 3.3 V output

A slight voltage overshoot is visible as the control loop comes into play. This was not regarded as serious enough to require correction.

Figure 22. 57 V shutdown full load



- Channel 1 = 12 V output
- Channel 2 = 3.3 V output

4.7.4 Transient response

Half load to full load transients were applied to the tested output with 50 V at the input. 16 sweeps were averaged by the oscilloscope to remove noise, which would otherwise obscure the traces.

Figure 23. 3.3 V half-full transient, 12 V at half load

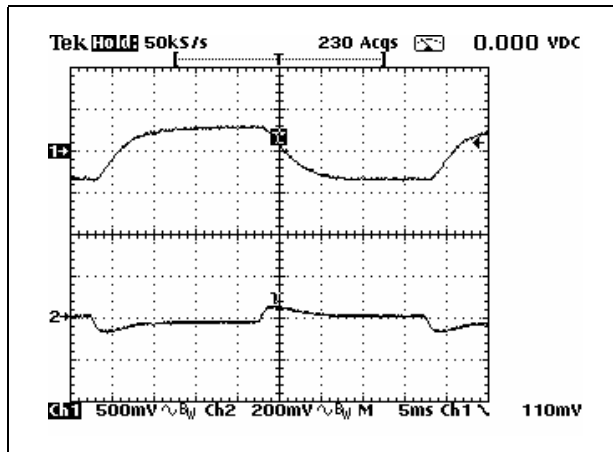
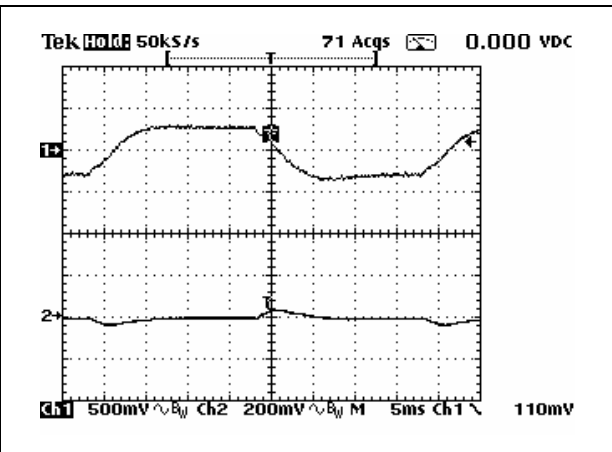


Figure 24. 12 V half-full transient, 3.3 V at half load



- Channel 1 = 12 V output
- Channel 2 = 3.3 V output

4.7.5 Overload characteristics

The STHS4257A1 limits the supply input current, thereby limiting the power to all outputs. If the current drawn by the converter exceeds 350 mA the STHS4257A1 will shut off and attempt to restart. As it continues to repeatedly recharge the power converter's input capacitors, it will shut down thermally.

The 12 V output is well protected from overload as it carries the bulk of the output power. In the short term, if it is sufficiently overloaded, the output voltage will fall on all windings of the transformer, including the bootstrap voltage for the L6565. If the bootstrap voltage goes low enough, the L6565 will shut itself off. It will attempt to restart when the bootstrap capacitor gets recharged to the L6565 startup voltage, and then turn off again.

If the 3.3 V output is shorted, the mechanism above will protect the unit. However, the 3.3 V output is not well protected against overload because it does not draw a large portion of the input power. It can supply well over its rated current for short terms, but if an overload remains in place the 3.3 V Schottky diode, the 3.3 V transformer winding, and the small filter choke will be overstressed.

4.7.6 Efficiency

- Full load = 78.2%
- Half load = 76.5%

Note that these figures include the losses in the LEDs and the input diodes.

4.8 Ripple and noise

Figure 25. Switching frequency ripple, two cycles shown

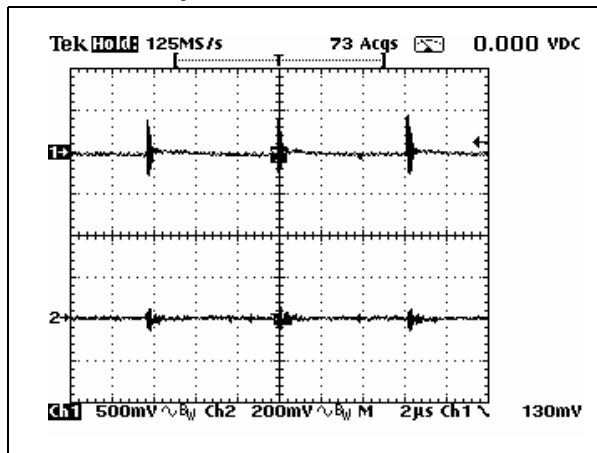
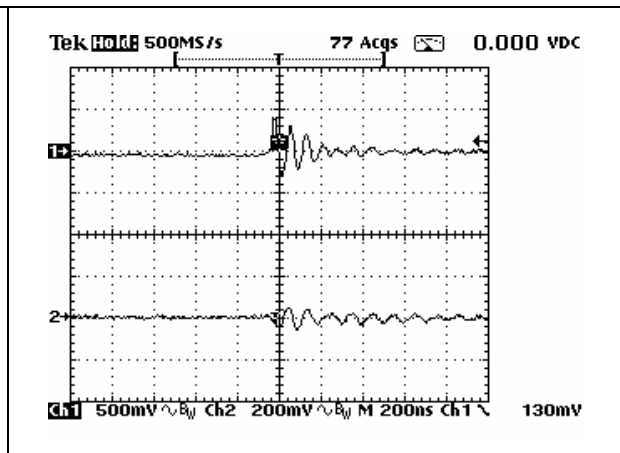


Figure 26. Expanded switching transient

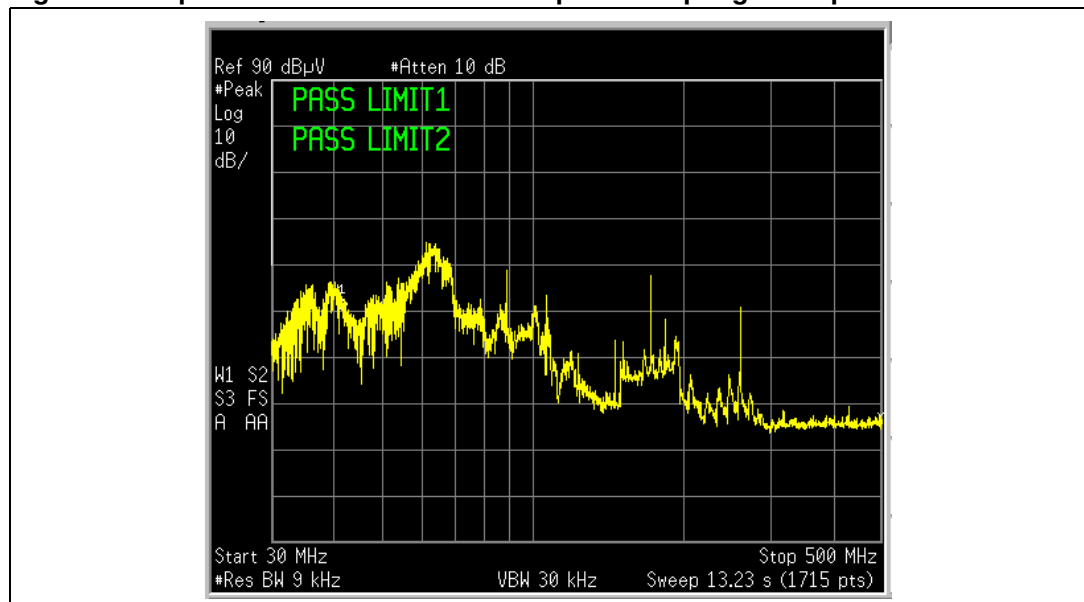


- Channel 1 = 12 V output
- Channel 2 = 3.3 V output

4.8.1 Radiated EMI

For an idea of the noise level the converter will place on the Ethernet cable, the noise between the two “ground” planes on the back of the PC board was measured. The signal was run directly into the 50 Ω input of a spectrum analyzer. Please ignore the pass limit notation.

Figure 27. Spectrum of noise between output and input ground planes



The noise level peaks at 54 dB, about 1/2 mV, at approximately 63 MHz. Radiated noise should not be a problem.

Appendix A Board layout

All board components are mounted on one side. All components are SMT except for mechanically stressed connectors.

The board includes 2 mm creepage and clearance spacing between PSE-connected circuits and load connected circuits (telecom network voltage - "TNV" isolation). The output RJ-45 connector (J2) is also isolated by 2 mm.

"Ground" planes are used on the bottom of the PC board, referenced to power converter return (negative) and output common. This simplifies the layout and provides local capacitive returns for noisy nodes such as the FET drain.

Design rules provide for 12 mil lines and 12 mil spaces.

Figure 28. Component placement

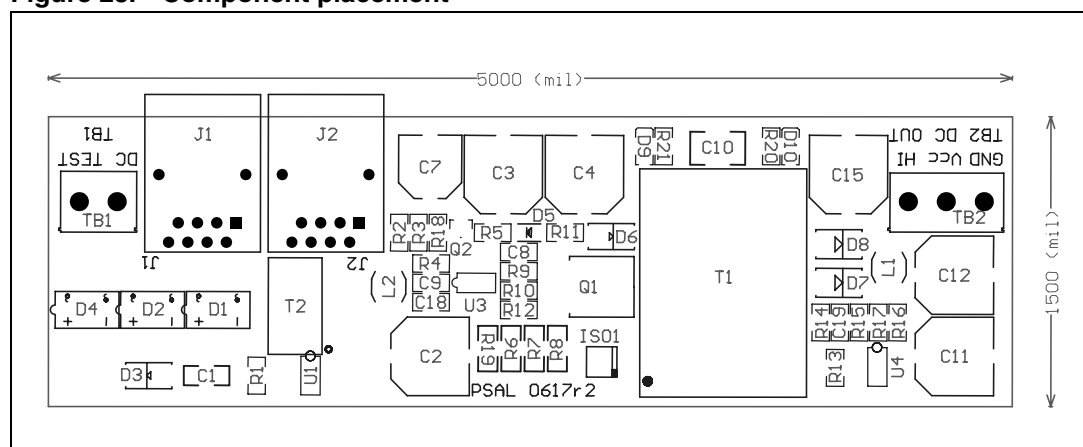


Figure 29. Top copper

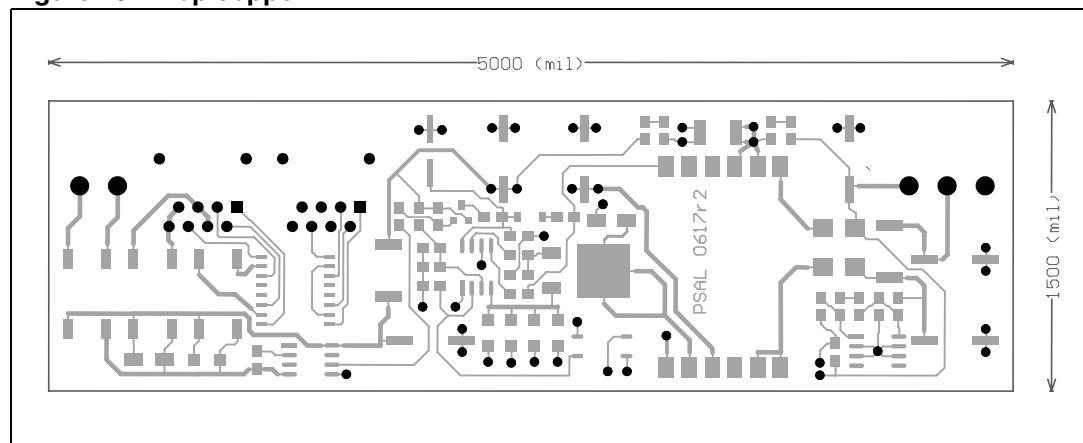


Figure 30. Bottom copper (mirrored)

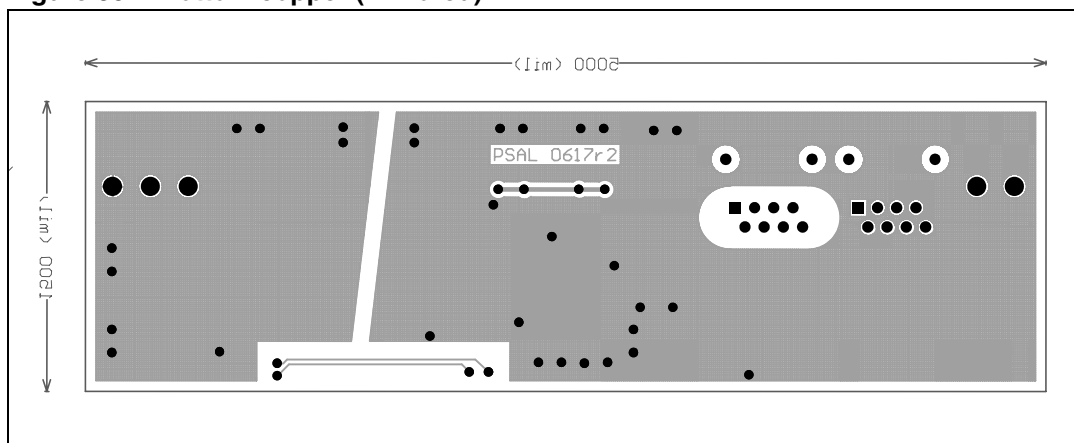
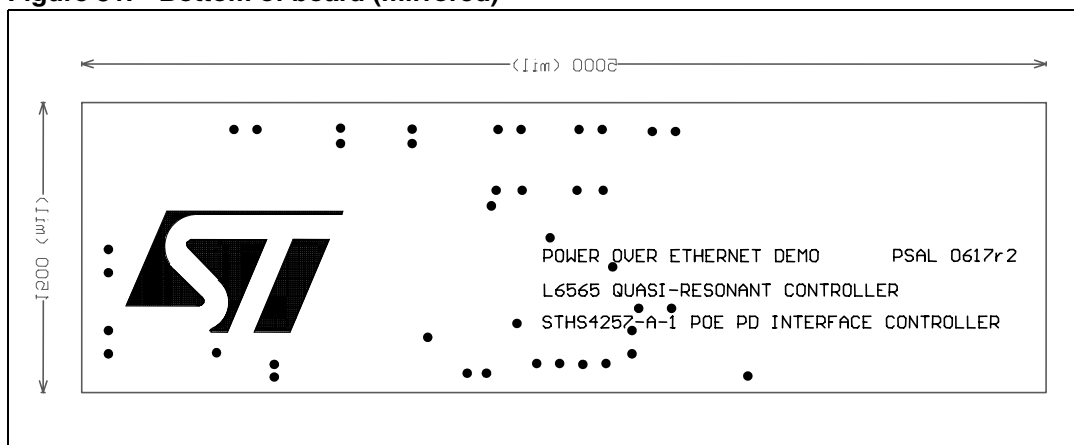


Figure 31. Bottom of board (mirrored)



Appendix B Bill of materials

Table 6. Bill of materials

Qty	Part type	Designator	Description	Mfg & Mfg #
1	0.1 uF 100 V 1206	C1	Capacitor 0.1 μ F 100 V	*
1	4700 pF Y 1812	C10	Capacitor 4700 pF 1 kv	Kemet C1812C472KDRACU
2	1500 μ F 6.3 V	C11,C12	Capacitor 1500 μ F 6.3 V	Panasonic EEV-FK0J152P
1	680 μ F 16 V	C15	Capacitor 680 μ F 16 V	Panasonic EEVFK1C681P
1	3300 pF 0805	C18	Capacitor	*
3	100 μ F 63 V	C2,C3,C4	Capacitor 100 μ F 63 V	Panasonic EEV-FK1J101P
1	47 μ F 25 V	C7	Capacitor 47 μ F 25 V	Panasonic EEV-HA1E470P
2	0.1 μ F 0805	C8,C19	Capacitor	*
1	0.01 μ F 0805	C9	Capacitor	*
3	BRIDGE DIP 1A	D1,D2,D4	1 A dip bridge	Diodes Inc DF1506DICT
1	LED GRN 0805	D10		Lumex SML-LXT0805GW-TR
1	SMAJ58A	D3	Zener diode	STMicroelectronics
1	1N4148W SOD123	D5	Diode	*
1	SMAJ188	D6	Zener diode	STMicroelectronics
1	STPS2L40U	D7	Schottky diode 2 A 40 V	STMicroelectronics
1	STPS3150U	D8	Schottky diode 3 A 150V	STMicroelectronics
1	LED YEL 0805	D9		Lumex SML-LXT0805YW-TR
1	PS2703-1_OPTO	ISO1	Optoisolator SMT	NEC PS2703-1-A
2	RJ45-8 FEMALE	J1,J2	RJ45-8 socket	Tyco-Amp 5557785-1
2	4.7 μ H	L1,L2	Inductor	Tyco-COEV DU6629-4R7M
1	STD5N20T4	Q1		STMicroelectronics
1	MMBT5401	Q2	PNP transistor 150 V	*
1	DNI 0805	R1	Classification resistor	Not used, class 0 reported
1	10 5% 0805	R11		*
1	47 k Ω 5% 0805	R12		*
1	1.00 k Ω 1% 0805	R13		*
1	2.21 k Ω 1% 0805	R14		*
1	100 5% 0805	R15		*
1	3.24 k Ω 1% 0805	R16		*
1	10.0 k Ω 1% 0805	R17		*
1	100 k Ω 5% 0805	R2		*
1	4.7 k Ω 5% 0805	R20		*

Table 6. Bill of materials (continued)

Qty	Part type	Designator	Description	Mfg & Mfg #
1	15 k Ω 5% 0805	R21		*
1	681 k Ω 1% 0805	R3		*
1	15.0 k Ω 1% 0805	R4		*
3	10 k Ω 5% 0805	R5,R10,R18		*
4	2.0 1206	R6,R7,R8,R19		*
1	22 5% 0805	R9		*
1	XFMR POE-15	T3	XFMR POE TAPPED SEC	Cramer N85158
1	XFMR POE SIG	T2		Pulse Eng. H2019
1	PHOENIX 2-PIN	TB1		Connect2
1	PHOENIX 3-PIN	TB2		Connect3
1	STHS4257-A-1 SO-8	U1	POE interface controller	STMicroelectronics
1	L6565D SO-8	U3	TRANS. MODE CTLLR	STMicroelectronics
1	TL431 SO-8	U4	TL431 PGM SHUNT REG	STMicroelectronics

Appendix C Bibliography

- IEEE 802.3af-2003, "Amendment: Data Terminal Equipment (DTE) Power via Media Dependent Interface (MDI)"
- "Power over Ethernet Eases Design Implementations", Power Electronics Technology magazine, November, 2003
- STMicroelectronics Application note AN1326, "L6565 QUASI-RESONANT CONTROLLER"
- STMicroelectronics Application note AN1376, "25W QUASI-RESONANT FLYBACK CONVERTER FOR SET-TOP BOX APPLICATION USING THE L6565"
- STMicroelectronics Application Note AN1439, "EVAL6565N, 30W AC-DC ADAPTER WITH THE L6565 QUASI-RESONANT PWM CONTROLLER"
- STMicroelectronics Application note AN2252, "Zero-voltage switching and emitter-switched bipolar transistor in a 3-phase auxiliary power supply"

Revision history

Table 7. Document revision history

Date	Revision	Changes
04-Apr-2007	1	First issue
08-Aug-2008	2	Added order code to the Introduction on page 1 . Minor text changes throughout the document.

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